

US009270510B2

(12) **United States Patent**
Ma et al.

(10) **Patent No.:** **US 9,270,510 B2**
(45) **Date of Patent:** ***Feb. 23, 2016**

(54) **ADAPTIVE TWO-DIMENSIONAL CHANNEL INTERPOLATION**

(71) Applicant: **Apple Inc.**, Cupertino, CA (US)
(72) Inventors: **Jianglei Ma**, Kanata (CA); **Ming Jia**, Ottawa (CA); **Wen Tong**, Ottawa (CA); **Peiyong Zhu**, Kanata (CA); **Hang Zhang**, Nepean (CA); **Hua Xu**, Nepean (CA); **Dong-Sheng Yu**, Ottawa (CA)

(73) Assignee: **Apple Inc.**, Cupertino, CA (US)

(*) Notice: Subject to any disclaimer, the term of this patent is extended or adjusted under 35 U.S.C. 154(b) by 0 days.

This patent is subject to a terminal disclaimer.

(21) Appl. No.: **13/944,022**

(22) Filed: **Jul. 17, 2013**

(65) **Prior Publication Data**

US 2014/0119471 A1 May 1, 2014

Related U.S. Application Data

(63) Continuation of application No. 13/665,982, filed on Nov. 1, 2012, which is a continuation of application

(Continued)

(51) **Int. Cl.**

H04L 27/26 (2006.01)
H04L 5/00 (2006.01)
H04L 25/02 (2006.01)

(52) **U.S. Cl.**

CPC **H04L 27/2611** (2013.01); **H04L 5/0007** (2013.01); **H04L 25/0232** (2013.01); **H04L 27/2626** (2013.01); **H04L 25/0226** (2013.01); **H04L 27/2647** (2013.01)

(58) **Field of Classification Search**

USPC 375/295, 260, 267, 299, 347, 349
See application file for complete search history.

(56) **References Cited**

U.S. PATENT DOCUMENTS

5,867,478 A 2/1999 Baum et al.
5,995,551 A 11/1999 Mccallister et al.

(Continued)

FOREIGN PATENT DOCUMENTS

CN 1448015 10/2003
EP 1081906 3/2001

(Continued)

OTHER PUBLICATIONS

Norte!, "Proposal for the Downlink Pilots for E-UTRA", 3GPP Draft, R1-051155, 3rd Generation Partnership Project (3GPP), Mobile Competence Centre, Oct. 4, 2005, pp. 1-33.

(Continued)

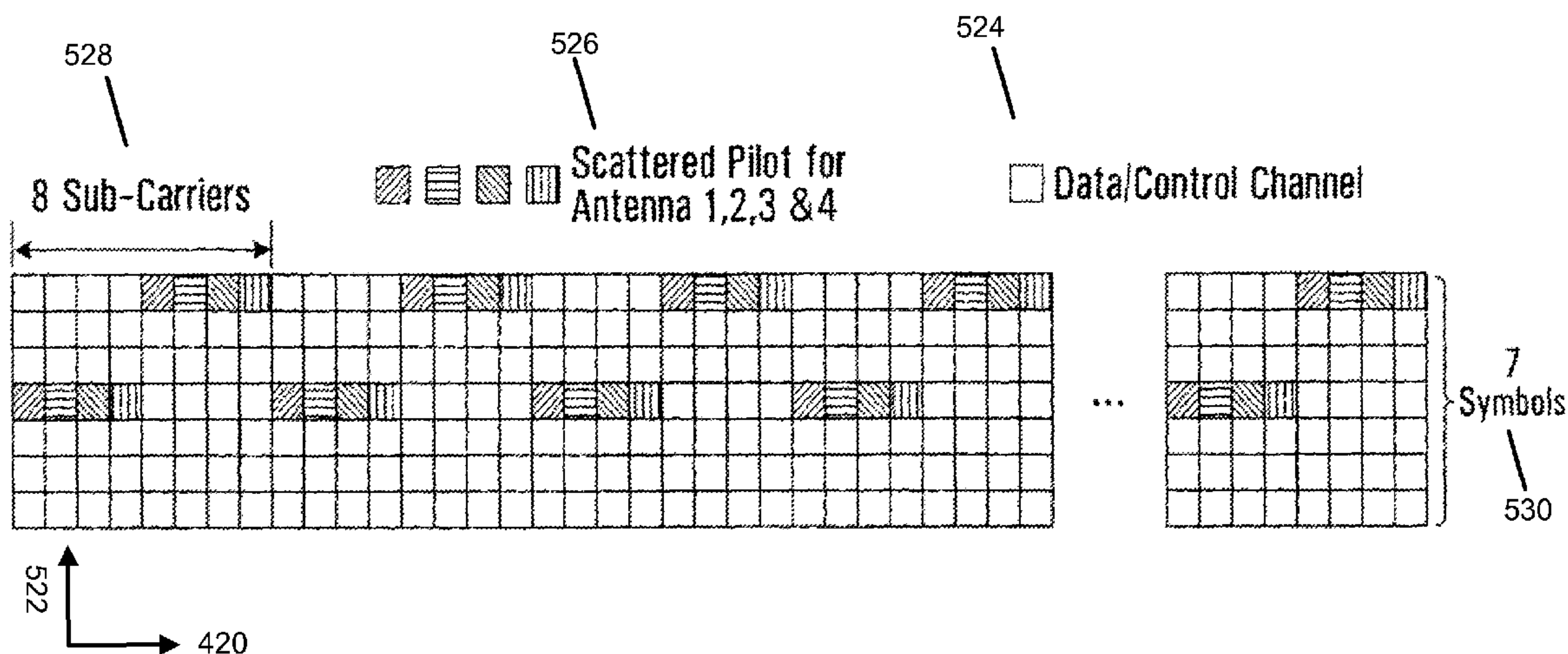
Primary Examiner — Kabir A Timory

(74) *Attorney, Agent, or Firm* — Meyertons, Hood, Kivlin, Kowert & Goetzel, P.C.

(57) **ABSTRACT**

A method and apparatus for improving channel estimation within an OFDM communication system. Channel estimation in OFDM is usually performed with the aid of pilot symbols. The pilot symbols are typically spaced in time and frequency. The set of frequencies and times at which pilot symbols are inserted is referred to as a pilot pattern. In some cases, the pilot pattern is a diagonal-shaped lattice, either regular or irregular. The method first interpolates in the direction of larger coherence (time or frequency). Using these measurements, the density of pilot symbols in the direction of faster change will be increased thereby improving channel estimation without increasing overhead. As such, the results of the first interpolating step can then be used to assist the interpolation in the dimension of smaller coherence (time or frequency).

14 Claims, 20 Drawing Sheets



Related U.S. Application Data

No. 12/064,566, filed as application No. PCT/CA2006/001380 on Aug. 22, 2006, now Pat. No. 8,331,465.
 (60) Provisional application No. 60/722,744, filed on Sep. 30, 2005, provisional application No. 60/710,527, filed on Aug. 23, 2005.

References Cited

U.S. PATENT DOCUMENTS

6,141,393 A 10/2000 Thomas et al.
 6,175,590 B1 1/2001 Stein
 6,188,717 B1 2/2001 Kaiser et al.
 6,215,813 B1 4/2001 Jones et al.
 6,215,827 B1 4/2001 Balachandran et al.
 6,298,035 B1 10/2001 Heiskala
 6,538,986 B2 3/2003 Isaksson et al.
 6,553,063 B1 4/2003 Lin et al.
 6,597,729 B1 7/2003 Schmidl et al.
 6,611,513 B1 8/2003 Ten Brink
 6,621,851 B1 9/2003 Agee et al.
 6,633,601 B1 10/2003 Yang
 6,650,694 B1 11/2003 Brown et al.
 6,654,429 B1 11/2003 Li
 6,662,337 B1 12/2003 Brink
 6,680,902 B1 1/2004 Hudson
 6,690,712 B2 2/2004 Kim et al.
 6,721,299 B1 4/2004 Song
 6,763,244 B2 7/2004 Chen et al.
 6,834,046 B1 12/2004 Hosur et al.
 6,865,232 B1 3/2005 Isaksson et al.
 7,085,314 B2 8/2006 Zhu et al.
 7,245,559 B2 7/2007 Ma et al.
 7,272,188 B2 9/2007 Lacroix-Penther et al.
 7,313,086 B2 12/2007 Aizawa
 7,433,433 B2 10/2008 Wilhelmsson et al.
 7,436,757 B1 10/2008 Wilson et al.
 7,751,510 B2 7/2010 Budianu et al.
 7,773,699 B2 8/2010 Jia et al.
 7,830,976 B2 11/2010 Gorokhov et al.
 8,027,243 B2 9/2011 Jin et al.
 8,238,956 B1 8/2012 Tang et al.
 8,254,246 B2 8/2012 Ma et al.
 2002/0051498 A1 5/2002 Thomas et al.
 2002/0183020 A1 12/2002 Zhu et al.
 2003/0036359 A1 2/2003 Dent et al.
 2003/0072254 A1* 4/2003 Ma et al. 370/208
 2003/0072255 A1 4/2003 Ma et al.
 2003/0072395 A1* 4/2003 Jia et al. 375/341
 2004/0001429 A1 1/2004 Ma et al.
 2004/0062191 A1 4/2004 Lacroix-penther et al.
 2004/0081073 A1 4/2004 Walton et al.
 2004/0085946 A1 5/2004 Morita et al.
 2004/0178934 A1 9/2004 Balakrishnan et al.
 2004/0190636 A1 9/2004 Oprea
 2004/0218682 A1 11/2004 Nam et al.
 2004/0246998 A1 12/2004 Ma et al.
 2005/0084042 A1 4/2005 Van Houtum
 2005/0105647 A1 5/2005 Wilhelmsson et al.
 2005/0163194 A1 7/2005 Gore et al.
 2005/0163238 A1 7/2005 Fujii
 2005/0202822 A1 9/2005 Park et al.
 2005/0265503 A1 12/2005 Rofheart et al.
 2006/0046734 A1 3/2006 Costa et al.
 2006/0067416 A1 3/2006 Tirkkonen et al.
 2006/0094460 A1 5/2006 Tiedemann, Jr. et al.
 2006/0105761 A1 5/2006 Walton et al.
 2006/0269016 A1 11/2006 Long et al.
 2007/0041456 A1 2/2007 Jahan et al.
 2007/0064669 A1 3/2007 Classon et al.
 2007/0155375 A1 7/2007 Kappel et al.
 2007/0258404 A1 11/2007 Tirkkonen et al.
 2008/0253279 A1 10/2008 Ma et al.
 2009/0225885 A1 9/2009 Aoki et al.

FOREIGN PATENT DOCUMENTS

EP 1198100 4/2002
 EP 1898542 3/2008
 FR 2742613 6/1997
 JP H07-020625 4/1995
 JP 2003-529238 9/2003
 JP 2007-502597 2/2007
 WO 9530289 11/1995
 WO 9908425 2/1999
 WO 0033504 6/2000
 WO 0126318 4/2001
 WO 02075955 9/2002
 WO 03/034642 4/2003
 WO 2004004269 1/2004
 WO 2004/049618 6/2004
 WO 2005022811 A2 3/2005
 WO 2005/057870 6/2005
 WO 2005/088882 9/2005
 WO 2005/125044 12/2005
 WO 2006/034577 4/2006

OTHER PUBLICATIONS

Takaoka S. et al., "Pilot-assisted adaptive interpolation channel estimation for OFDM signal reception", Vehicular Technology Conference, May 17, 2004, pp. 1777-1781.
 International Search Report filed in Application No. PCT/CA2006/001380, mailed on Nov. 24, 2006, pp. 1-2.
 International Search Report in Application No. PCT/CA2006/001595, Jan. 19, 2007, pp. 2-5.
 Non-Final Office Action in corresponding U.S. Appl. No. 111992,737, Jan. 3, 2012, pp. 1-11.
 Final Office Action in corresponding U.S. Appl. No. 111992,737, Oct. 24, 2012, pp. 1-13.
 International Search Report in Application No. PCT/CA2006/001383, Dec. 15, 2006, pp. 2-4.
 Mino et al.; "Winner II intramode and intermode cooperation schemes definition," Winner II D4.8.1 v1.0, Information Society Technologies (IST-4-027756), Jun. 30, 2006; pp. 1-79.
 Office Action in corresponding U.S. Appl. No. 12/064,563, Apr. 26, 2011, pp. 1-15.
 Non-Final Office Action in corresponding U.S. Appl. No. 13/292,643, Feb. 1, 2013, pp. 1-19.
 "Physical Layer Aspects for Evolved UTRA (Release 7);" 3rd Generation Partnership Project, Technical Specification Group Radio Access Network, 3GPP TR 25.814 V0.1.1, Jun. 2005; pp. 1-28.
 Communication in EP Application No. 08 075 282.7-2415, Jul. 1, 2002/0051498 A1 2010, pp. 1-4.
 "Physical Channel Concept for Scalable Bandwidth in Evolved UTRA Downlink;" NTT DoCoMo, 3GPP TSG RAN WG 1 Ad Hoc on LTE, Sophia Antipolis, France, Jun. 20-21, 2005; pp. 1-14.
 "Requirements for Evolved UTRA (E-UTRA) and Evolved UTRAN (E-UTRAN) (Release 7);" 3rd Generation Partnership Project; Technical Specification Group Radio Access Network; 3GPP TR 25.913 v.7.0.0, Jun. 2005; pp. 1-15.
 Ericsson et al., "Text Proposal on Cell Search in Evolved UTRA", 3GPP Draft; R1-051308 JTP Cell Search, 3rd Generation Partnership Project (3GPP), Mobile Competence Centre; Nov. 1, 2005, pp. 1-4.
 3GPP TR 25.913, 3rd Generation Partnership Project; Technical Specification Group Radio Access Network; Requirements for Evolved UTRA (E-UTRA) and Evolved UTRAN (E-UTRAN), V7.0.0, Jun. 1, 2005, pp. 1-15.
 Office Action from Japanese Patent Application No. 2010-528205, mailed May 22, 2013, (English Translation), pp. 1-3.
 Ericsson et al., "UE Capability on Supportable Bandwidths", 3GPP Draft; R1-051309 UE Capability, 3rd Generation Partnership Project (3GPP), Mobile Competence Centre, Nov. 1, 2005, pp. 1-6.
 Norte!, "Proposal for initial access channel for E-UTRA (SCH and BCH)", 3GPP TSG RANWG1 L TE ad hoc, Jan. 18, 2006, pp. 1-18.
 NTT DoCoMo, "Cell Search Method in Connected and Idle Mode for E-UTRA Downlink", 3GPP Draft; R1-060163 DL Cell Search Operation in Idle Mode, 3'd Generation Partnership Project (3GPP), Mobile Competence Centre, Jan. 19, 2006, pp. 1-3.

(56)

References Cited

OTHER PUBLICATIONS

Nortel, "Proposal for the Downlink Synchronization Channel Design for E-UTRA", 3GPP TSG RAN WG 1 data base, Aug. 24, 2005, pp. 1-12.

Texas Instruments, "Downlink Synchronization Channel Schemes for E-UTRA", 3GPP Draft, R1-050725 _Cell Search, 3'd Generation Partnership Project (3GPP), Mobile Competence Centre, Aug. 25, 2005, pp. 1-12.

NTT DoCoMo, "Physical Channels and Multiplexing in Evolved UTRA Downlink", 3GPP Draft; R1-050590 Physical Channels and Multiplexing in DL, 3'd Generation Partnership Project (3GPP), Mobile Competence Centre, Jun. 16, 2005, pp. 1-24.

ZTE, "Comparing of Two Downlink Synchronization Channel Schemes for E-UTRA", 3GPP Draft, R1-051357 Comparing of Downlink Synchronization Channel Schemes for E-UTRA, 3'd Generation Partnership Project (3GPP), Mobile Competence Centre, Oct. 31, 2005, pp. 1-6.

Texas Instrument, "An alternative scheme to detect the STID encoding of PCCPCH", TSG-RAN WG 1 Meeting 3, Mar. 26, 1999, URL: http://www.3gpp.org/ftp/tsg_ran/WG1_RL1/TSGR1_03/Docs/pdfs/RI99150.PDF, pp. 1-5.

Nortel, "BCH Detection Performance Evaluation". 3GPP TSG-RAN working group 1 meeting 46, Sep. 1, 2006, URL: http://www.3gpp.org/ftp/tsg_ran/WG1_RL1/TSGR146/Docs/R1-062141, pp. 1-7.

Dabak A. G. et al., "A comparison of the open loop transmit diversity schemes for third generation wireless systems", Wireless communications and networking conference, 2000, WCNC, 2000 IEEE, Sep. 23-28, 2000, pp. 437-442.

Danunann A. et al., "Transmit/Receive-antenna diversity techniques for OFDM systems", European Transactions on Telecommunications, Wiley & Sons, Chichester, GB, vol. 13, No. 5, Sep. 1, 2002, pp. 531-538.

Fernandez "Efficient Pilot Patterns for Pilot Estimation in OFDM Systems over HF Channels" (VTC 1999) Gateway to the 21st. Century Communications Village, vol. 1•4 Con F. 50, Sep. 19, 1999-Sep. 22, 1999, pp. 2193-2197.

3GPP TR 25.814 vol.1 "3rd Generation Partnership Project; Technical Specification Group Radio Access Network; Physical Layer Aspects for Evolved UTRA (Release 7)" (Jun. 2005), pp. 1-28.

V. Mignone et al. "CD3-OFDM: A New Channel Estimation Method to Improve the Spectrum Efficiency in Digital Terrestrial Television Systems", International Broadcasting Convention, Sep. 14-18, 1995; XP 000617513; pp. 122-128.

Jones V K et al.: "Channel Estimation for Wireless OFDM Systems", IEEE GLOBECOM vol. 2, Nov. 1998, pp. 980-985.

European Search Report for corresponding European Patent Application No. 06790759.2, Feb. 13, 2013, pp. 1-7.

U.S. Appl. No. 10/038,916, filed Jan. 8, 2002, Ming Jia.

Non-Final Office Action in corresponding U.S. Appl. No. 12/064,566, Mar. 24, 2011, pp. 1-9.

European Search Report for corresponding European Patent Application No. 08075282.7, dated Jul. 1, 2010, pp. 1-4.

European Search Report issued Apr. 13, 2010 from corresponding European Patent No. 06790759.2, pp. 1-2.

European Search Report issued Apr. 13, 2010 from corresponding European Patent No. 08075276.9, pp. 1-3.

U.S. Appl. No. 12/839,836, filed Jul. 20, 2010, Ming Jia.

U.S. Appl. No. 13/437,066, filed Apr. 2, 2012, Ming Jia.

European Search Report in application No. 06790566.1 mailed Apr. 7, 2013, pp. 1-8.

"Proposal for the Downlink Pilots for E-UTRA" RI-050893 3GPP, Sep. 2, 2005, pp. 1-29.

"Pilot Channel and Scrambling Code in Evolved UTRA Downlink" RI-050589 3GPP, Jun. 20-21, 2005, pp. 1-24.

Office Action from Chinese Application No. 201310048966.8, issued Apr. 27, 2015, English and Chinese versions, pp. 1-10.

Notification of Reexamination, Chinese Application No. 201110120817.9, mailed Jul. 31, 2015, 25 pages.

* cited by examiner

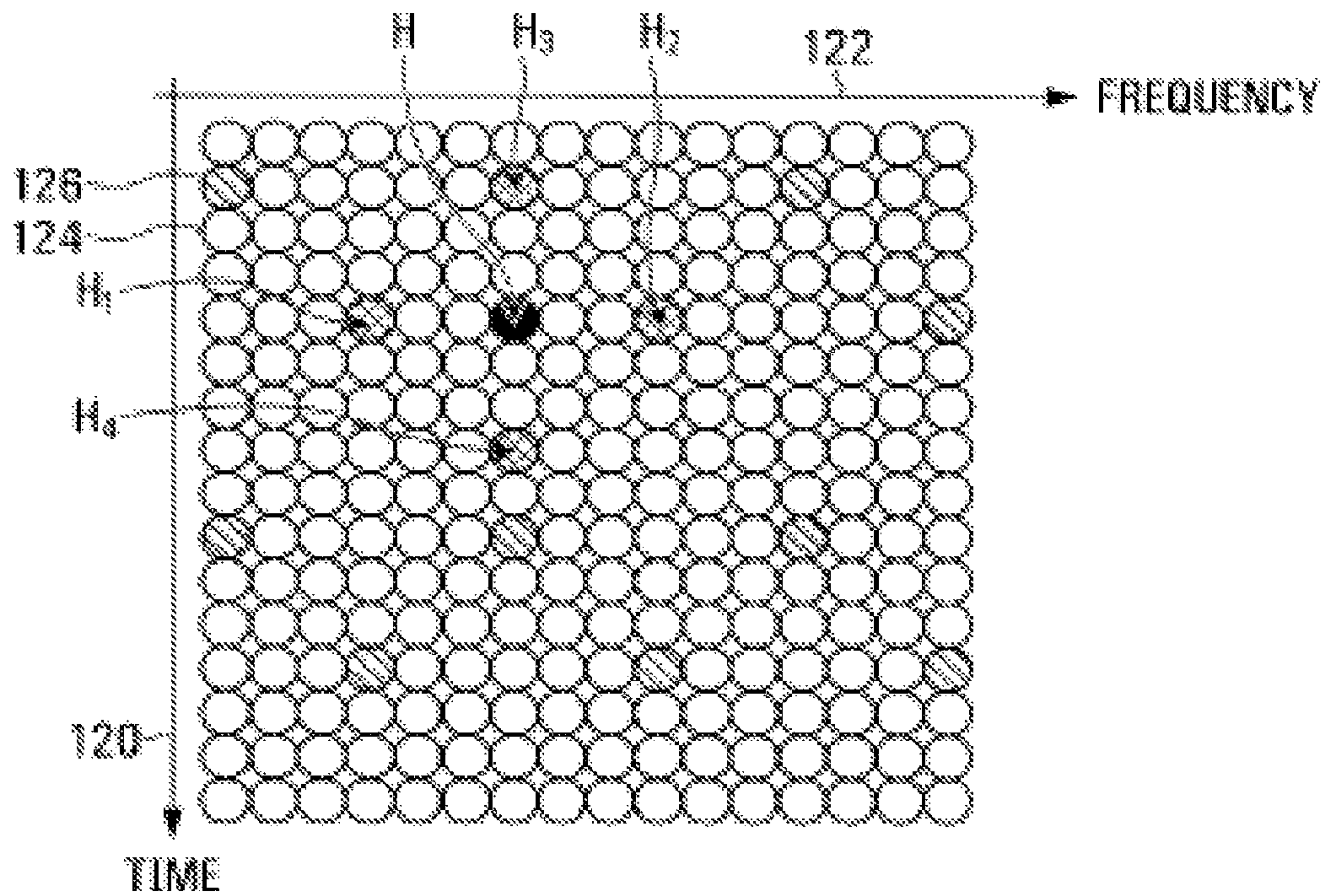


Figure 1

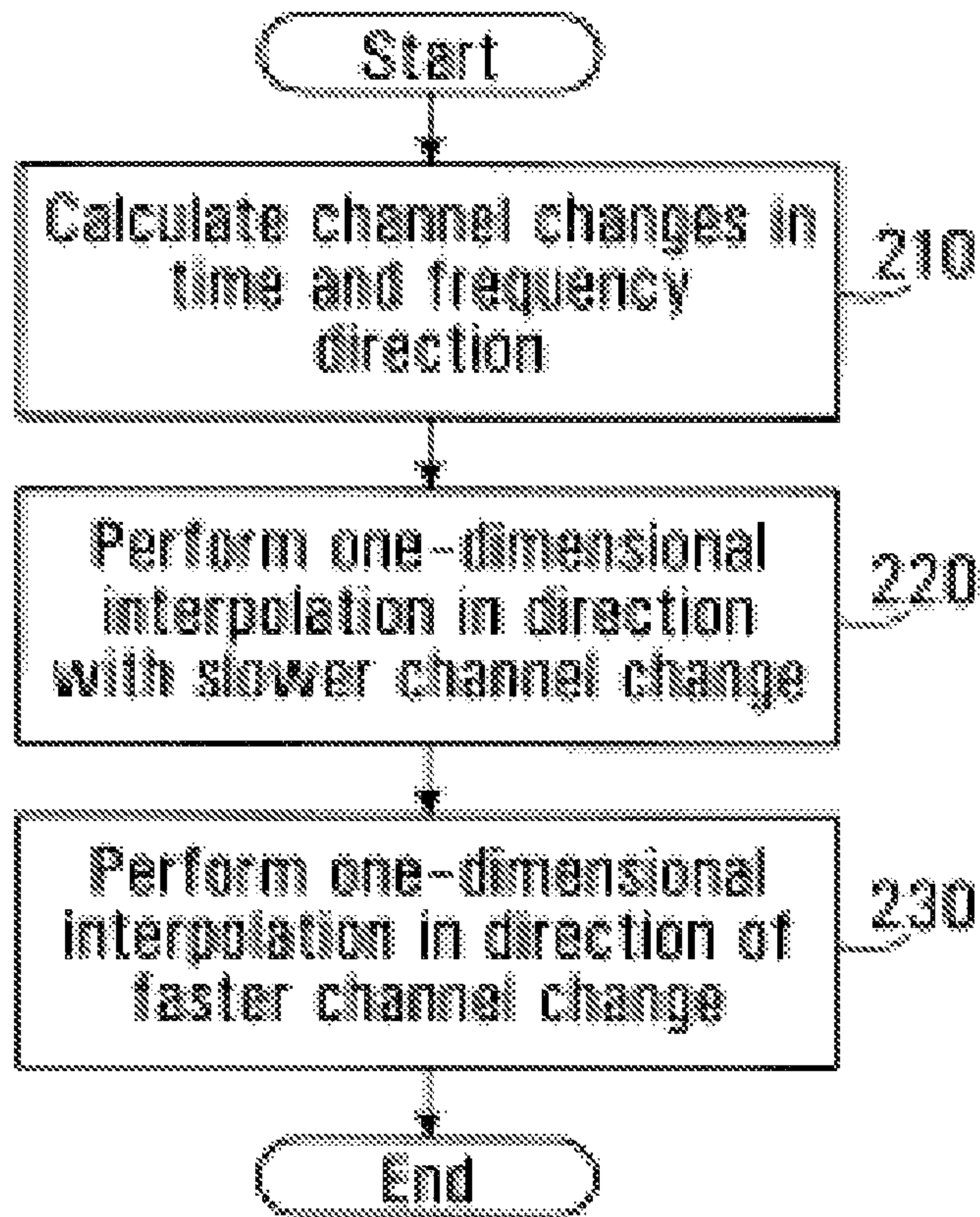


Figure 2

Pilot and Channel Estimation: VA 350 km/h
1x2 MRC, CTC 2/3, QAM-64, 1/28

- ◆ S. Pilot, with adapt.
- S. Pilot, without adapt.
- * Ideal Channel

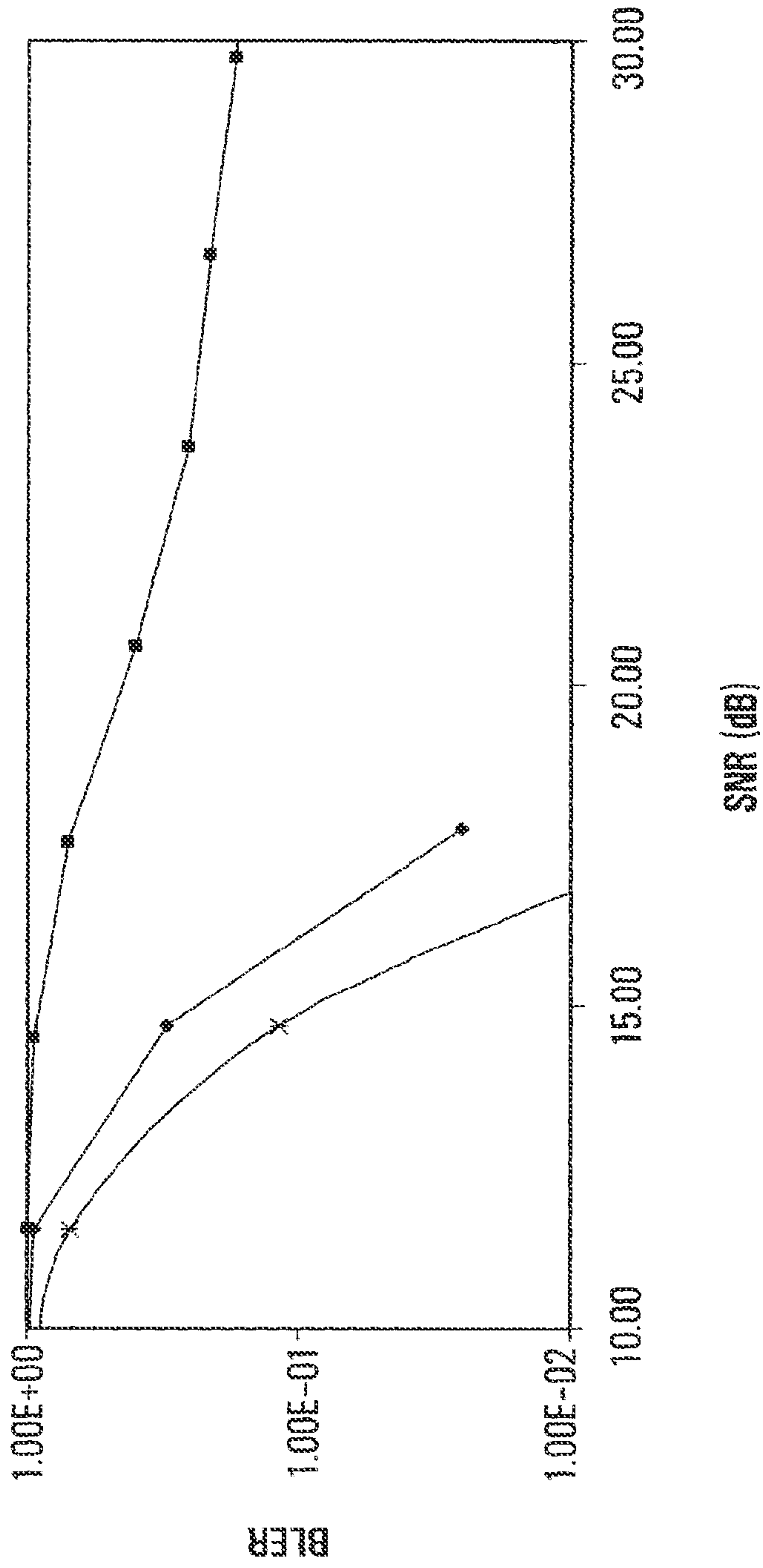


FIG. 3

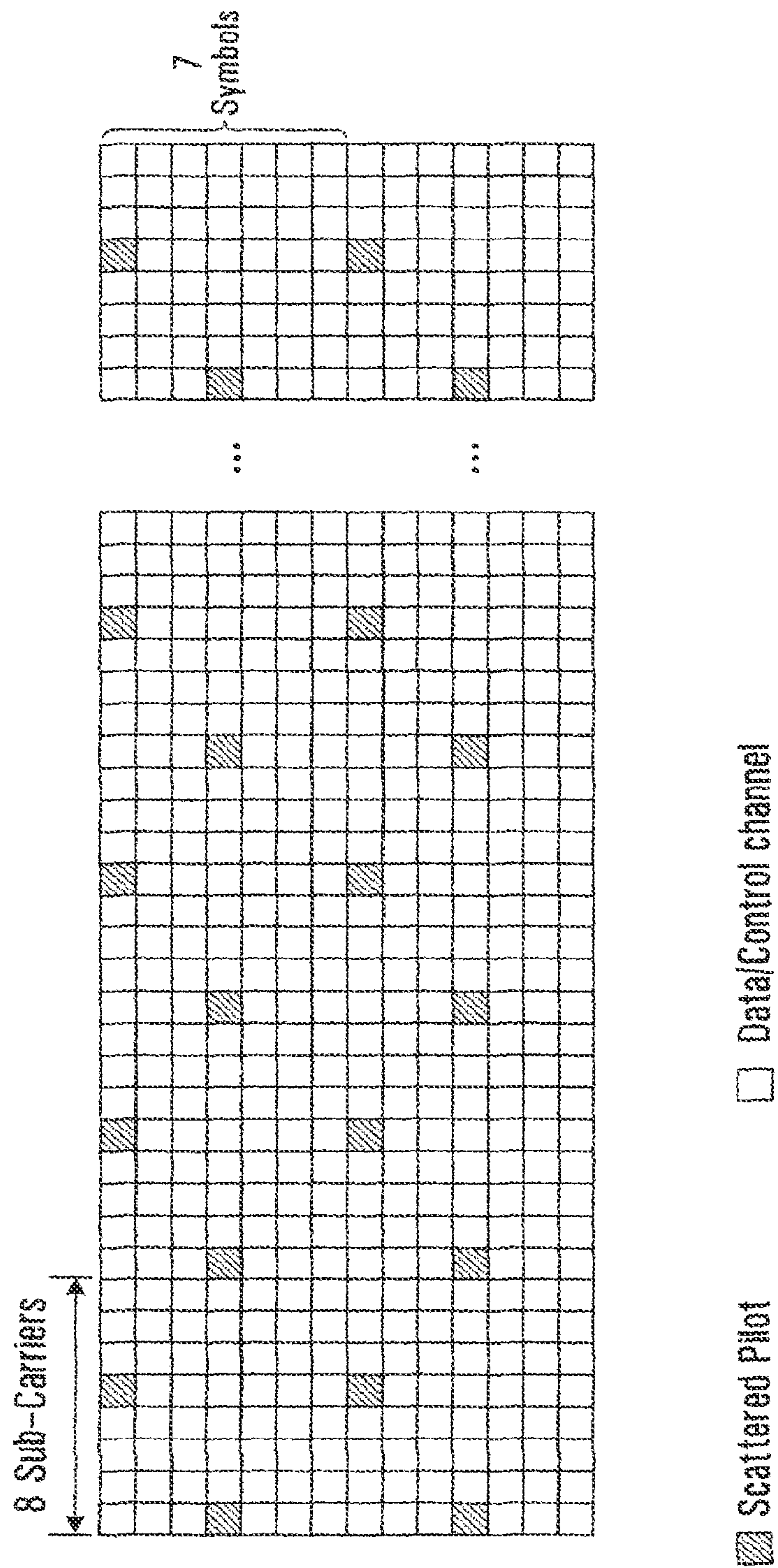


FIG. 4A

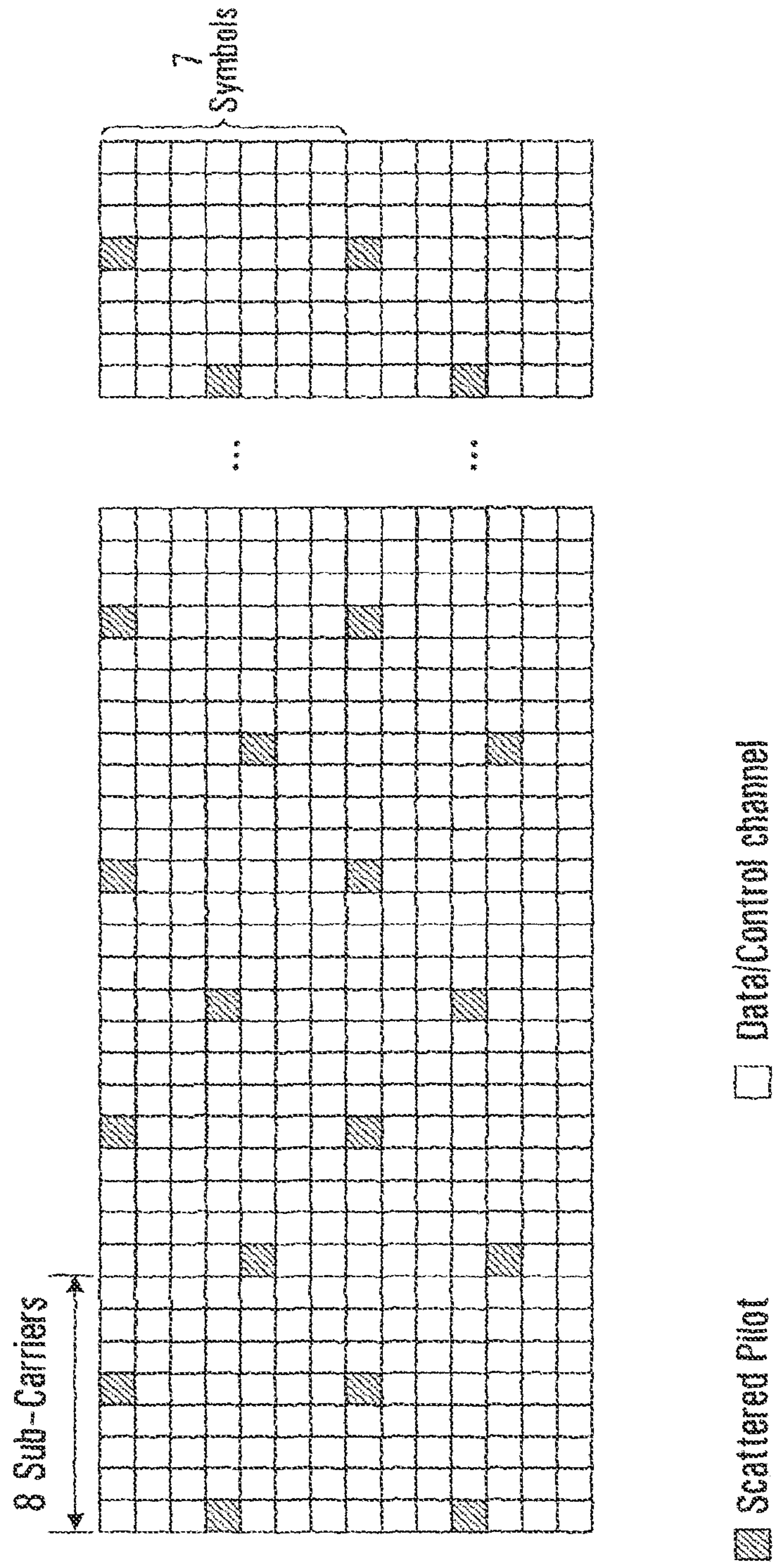


FIG. 4B

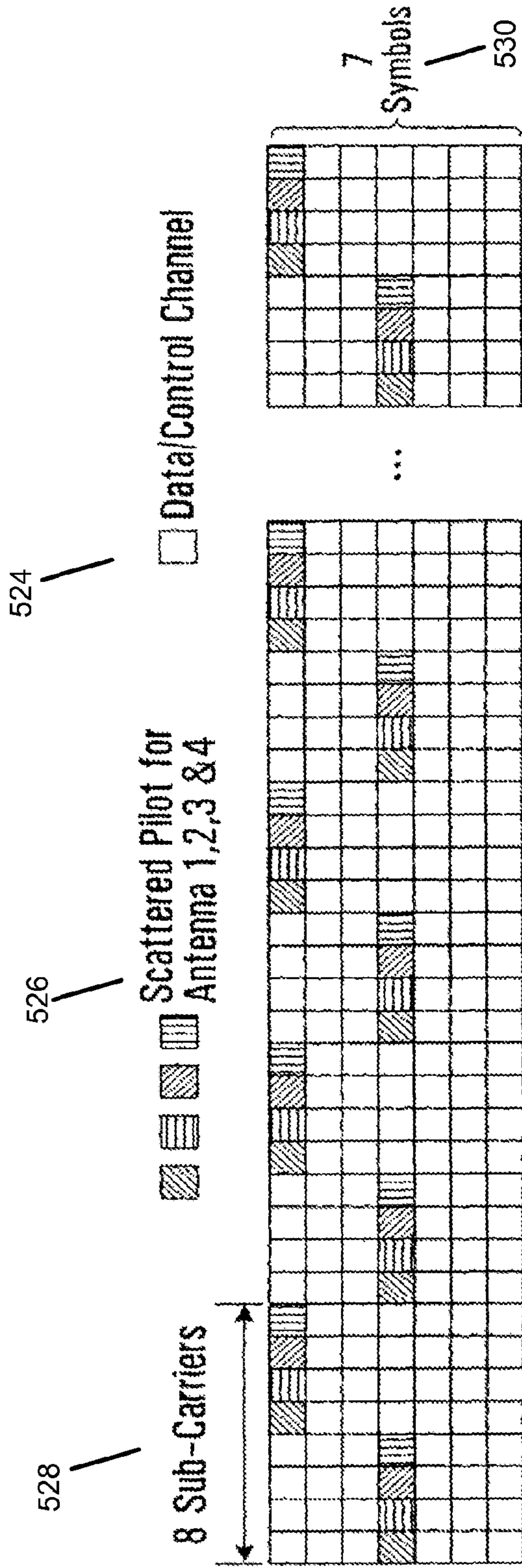


FIG. 5A

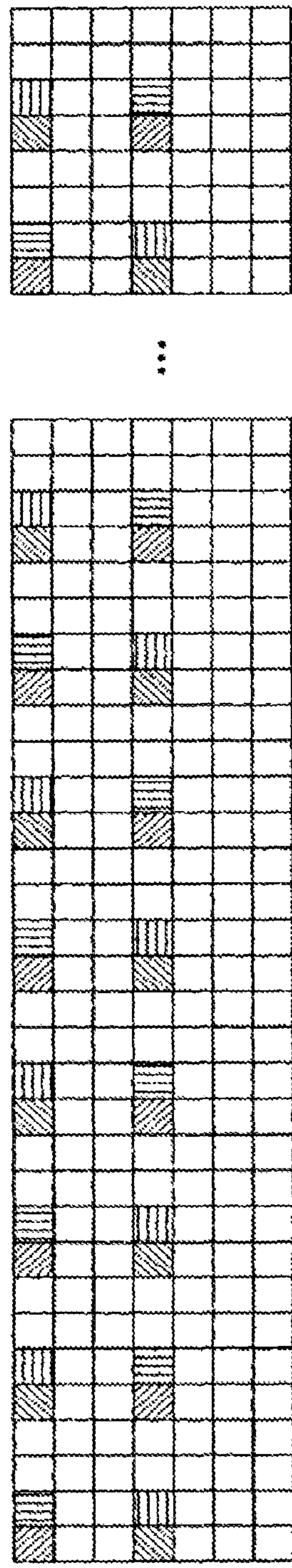
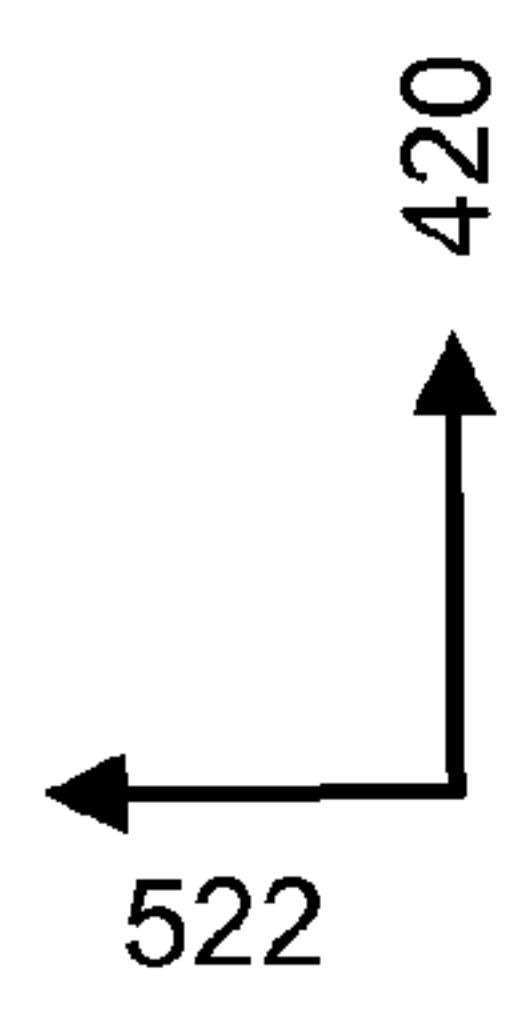


FIG. 5B

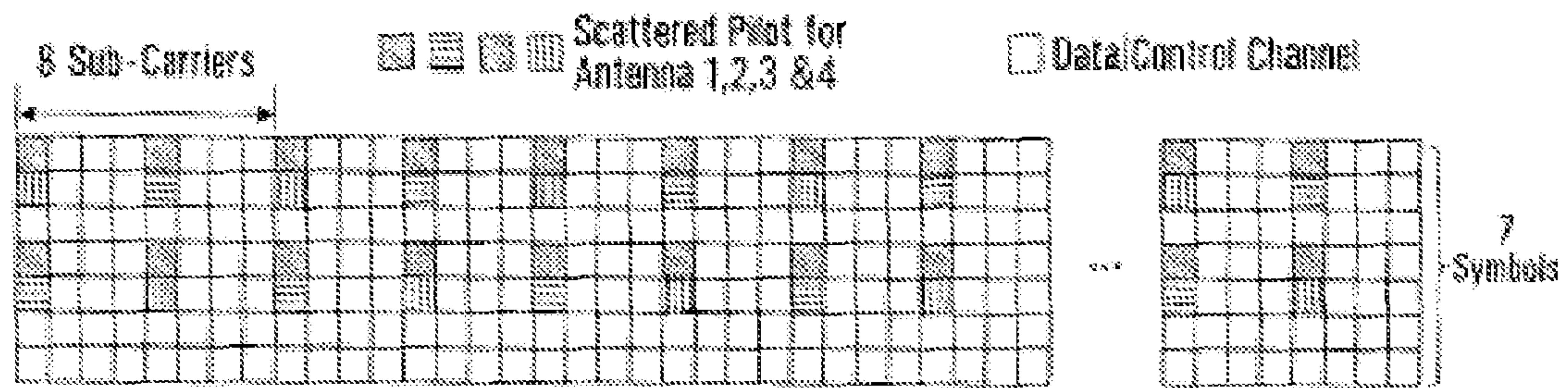


Figure 5C

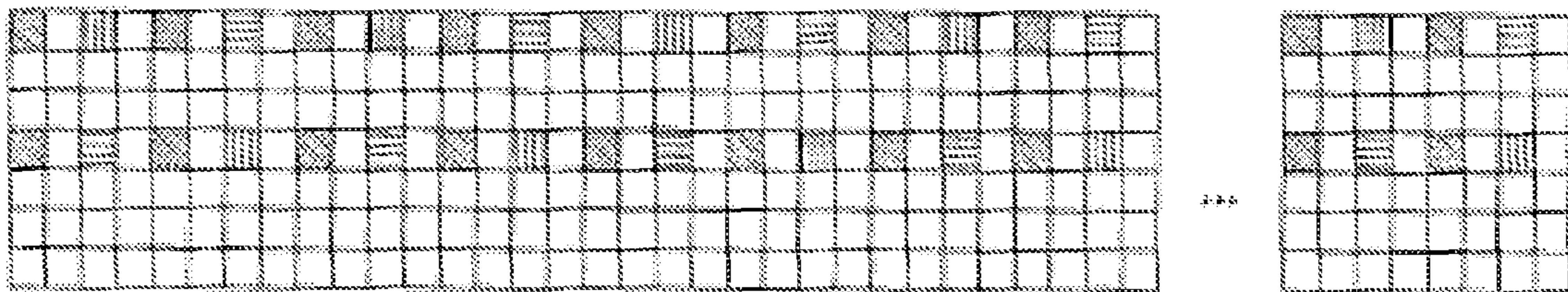


Figure 5D

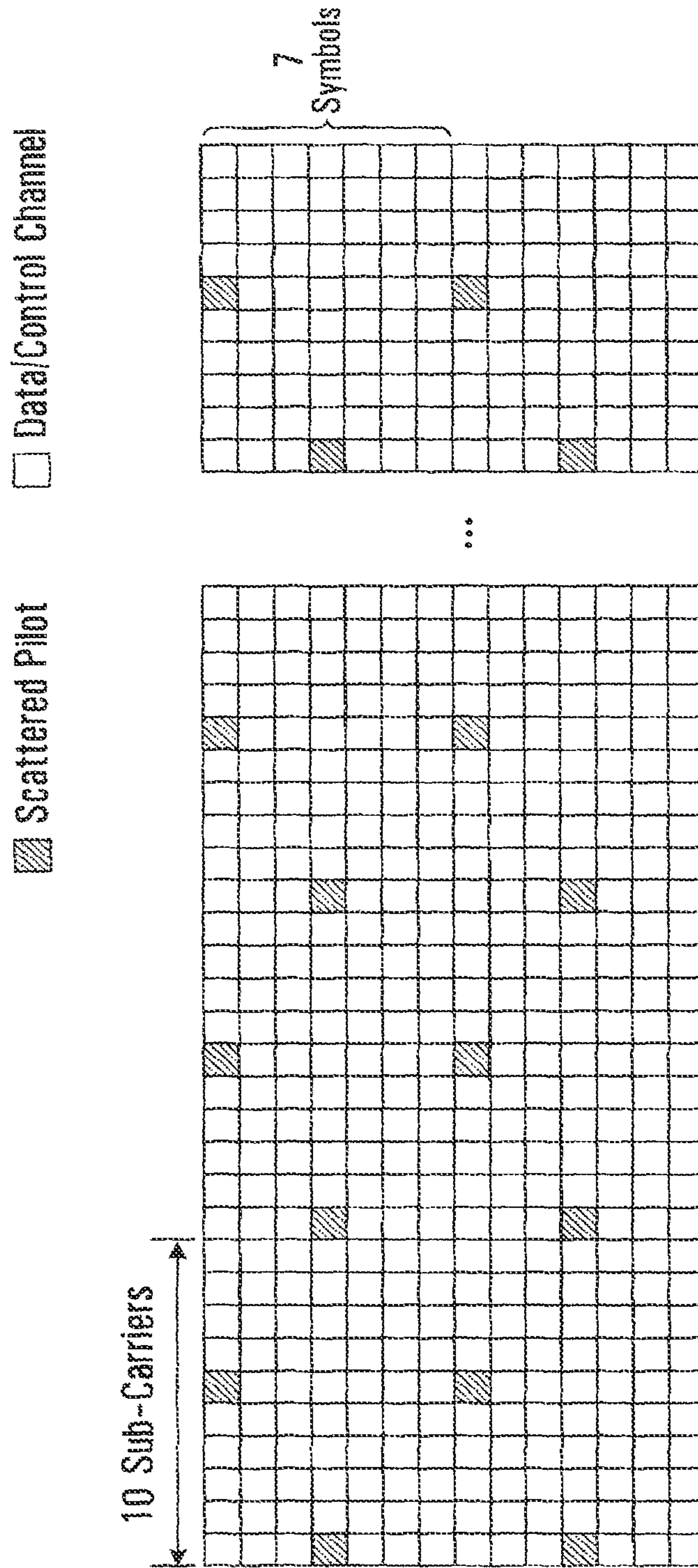


FIG. 6

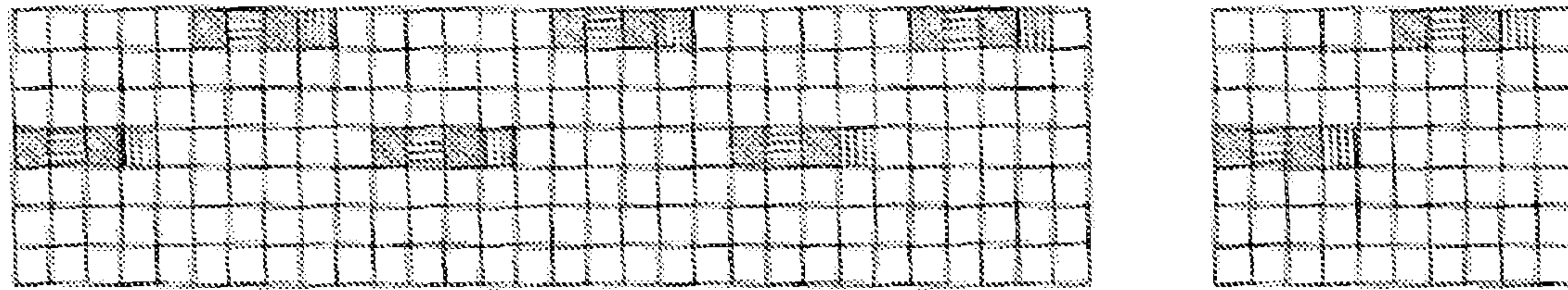


Figure 7A

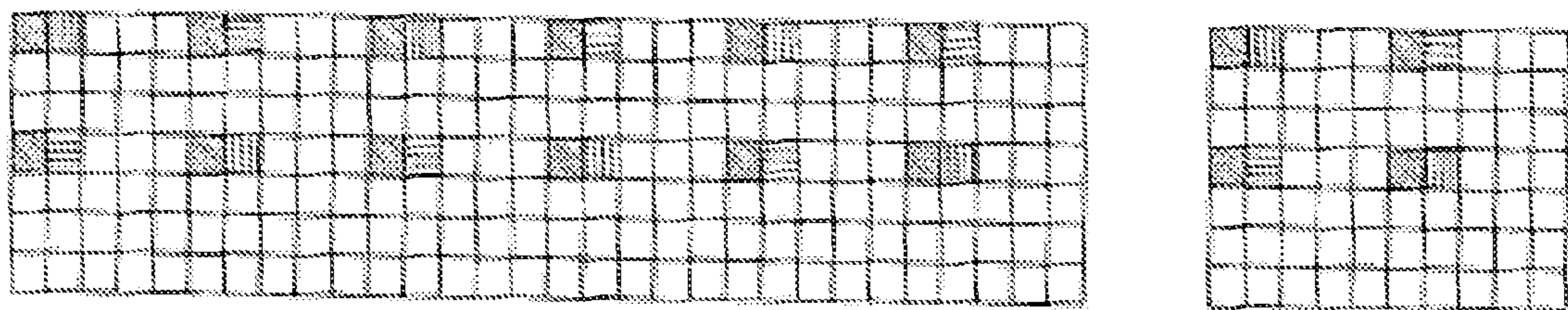


Figure 7B

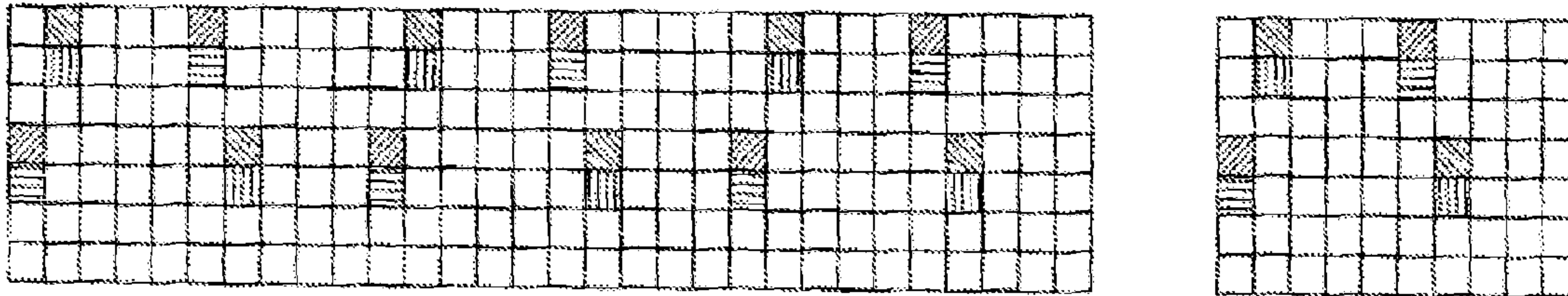


Figure 7C

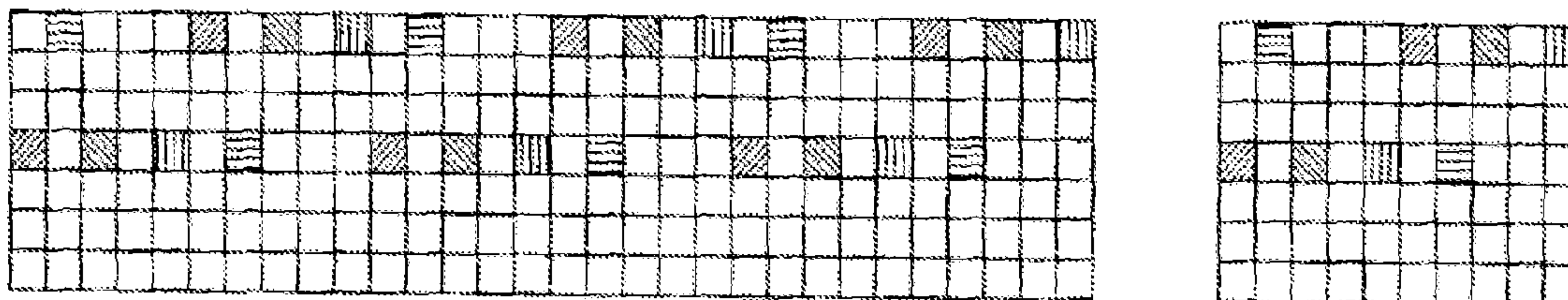


Figure 7D

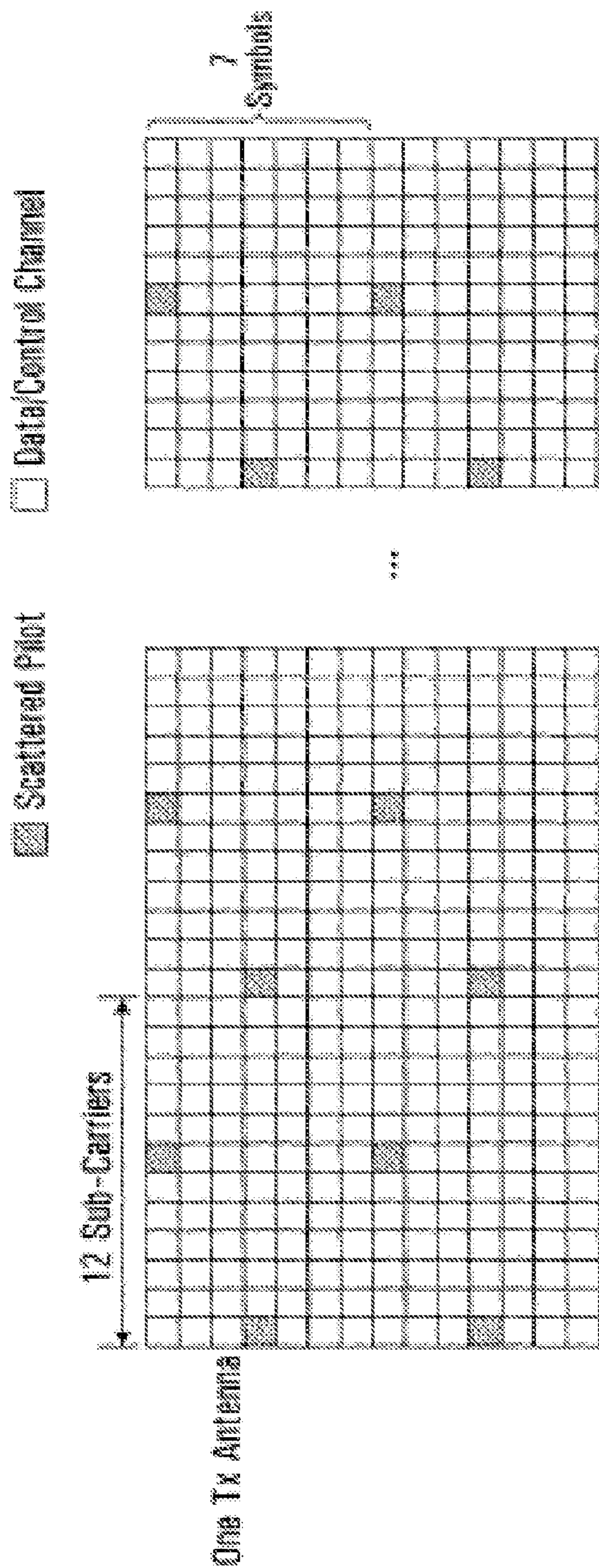


Figure 8

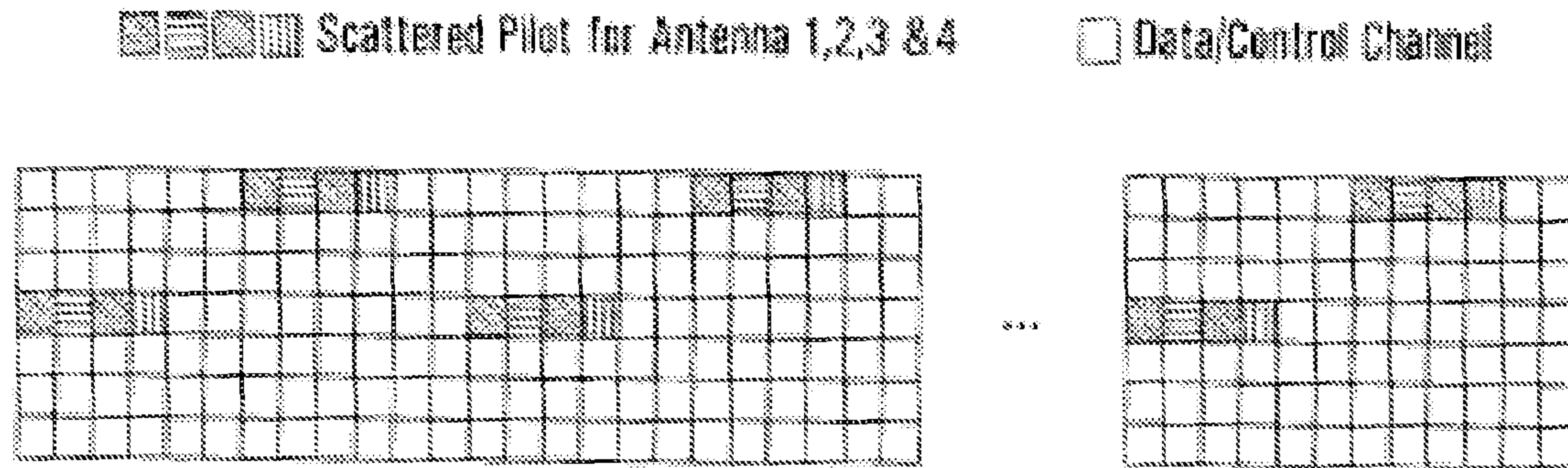


Figure 9A

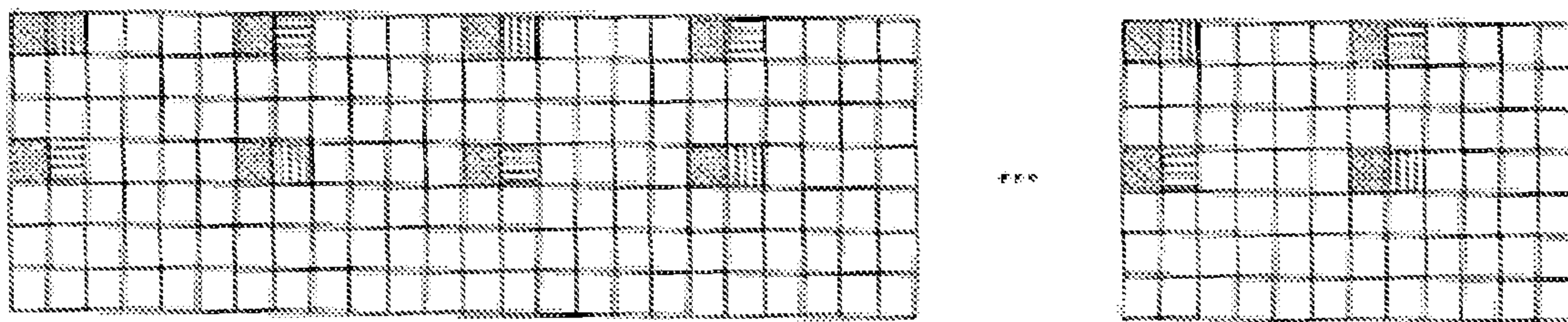


Figure 9B

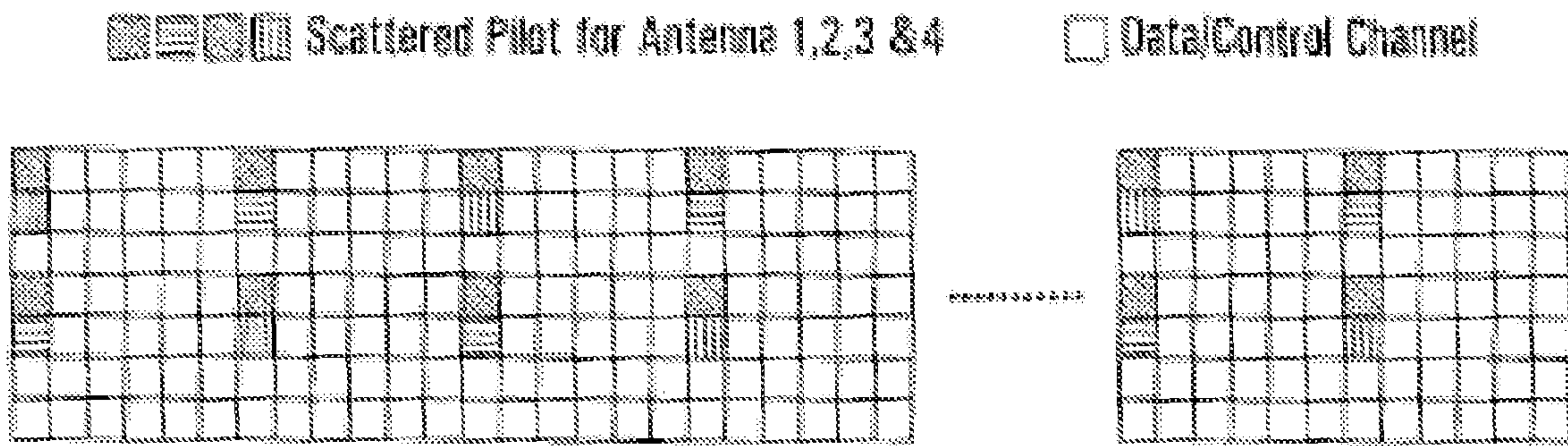


Figure 9C

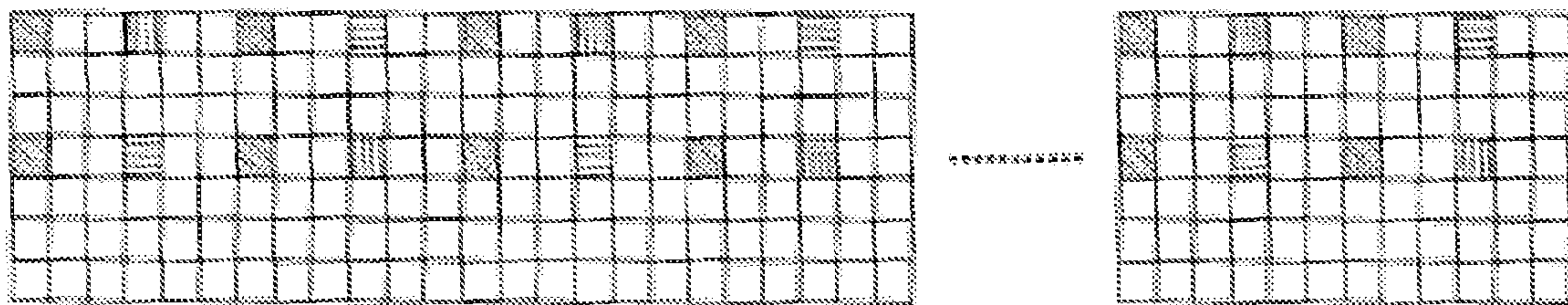


Figure 9D

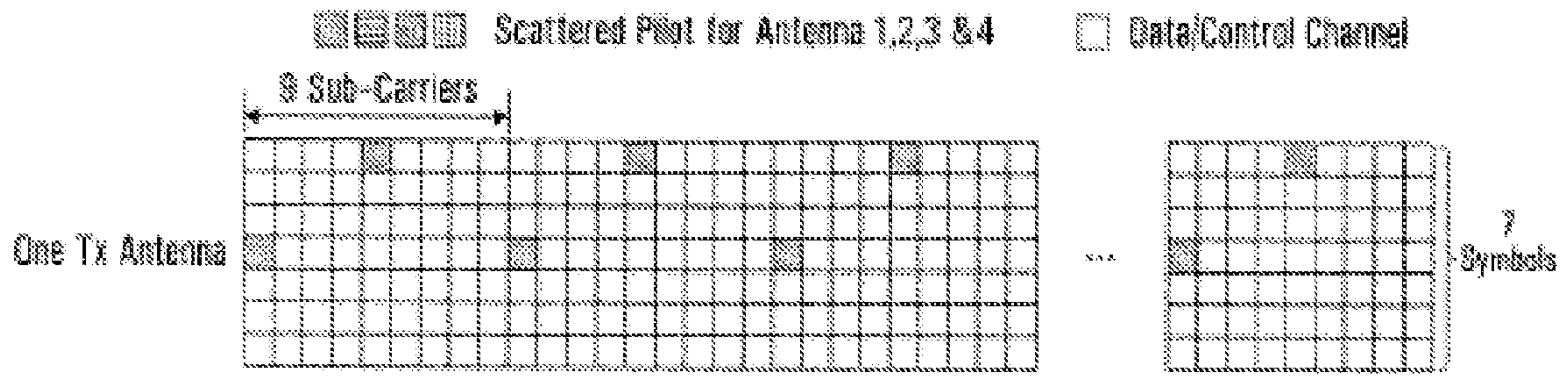


Figure 10A

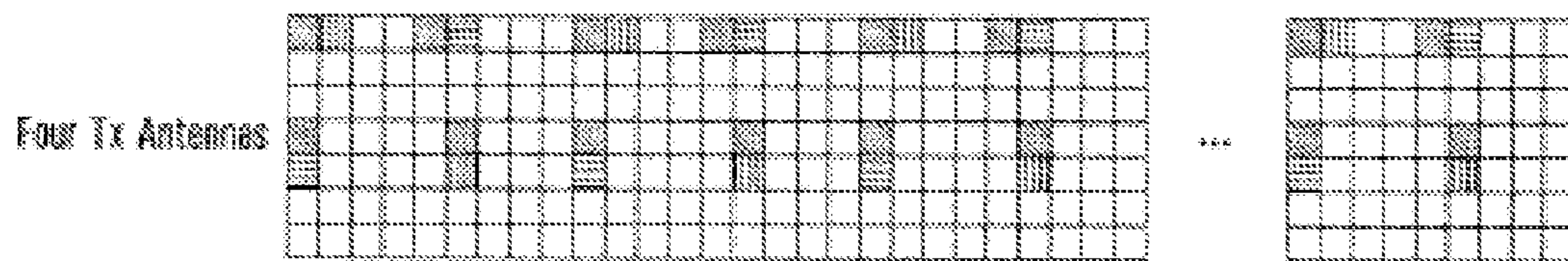


Figure 10B

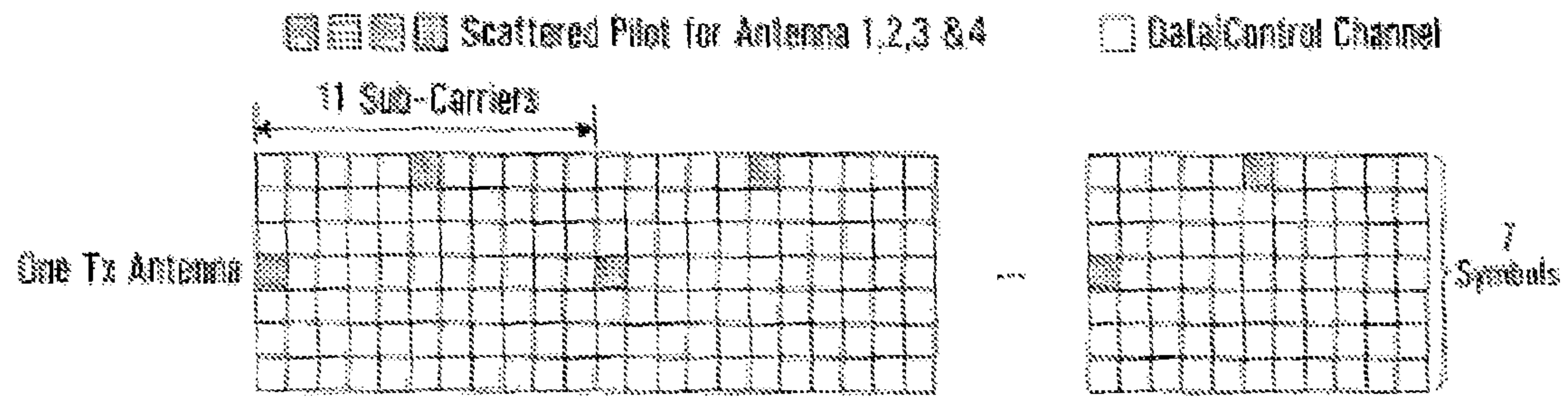


Figure 11A

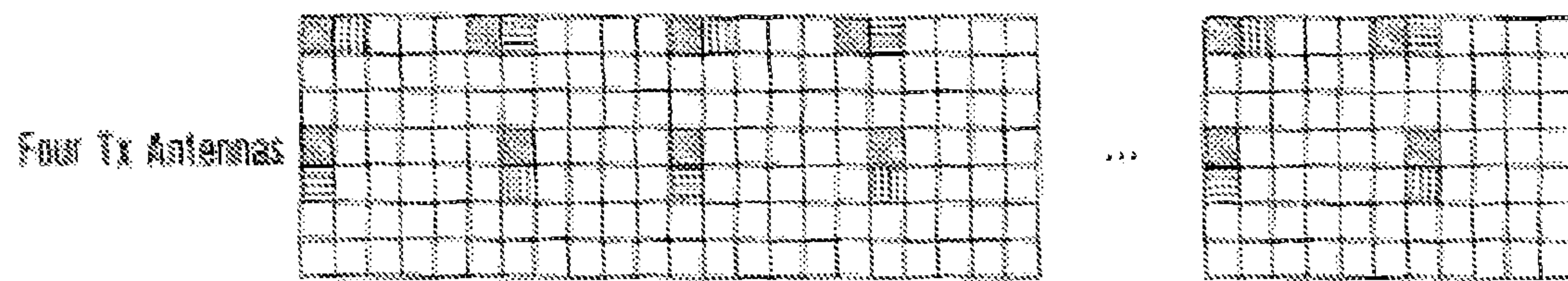


Figure 11B

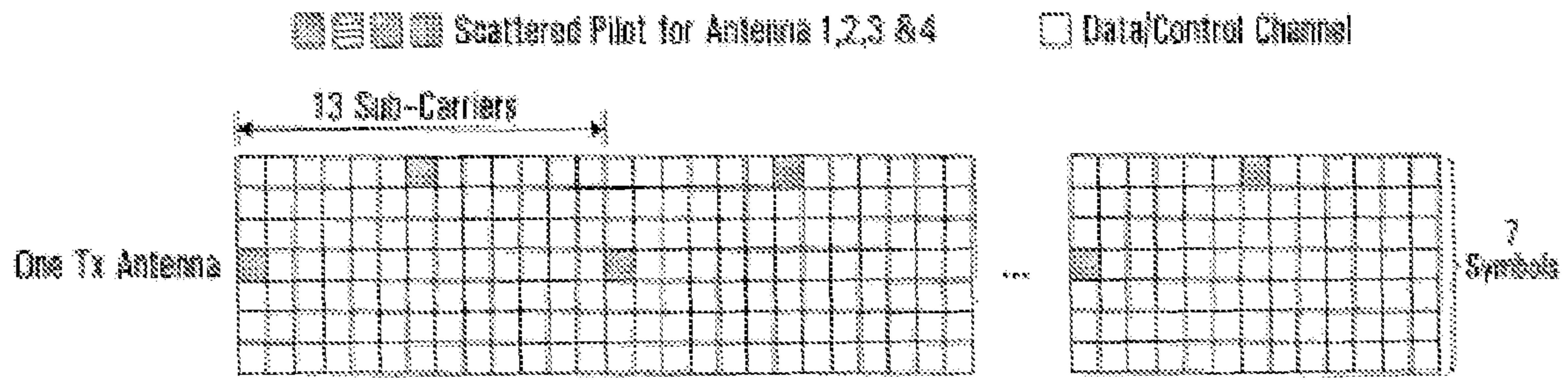


Figure 12A

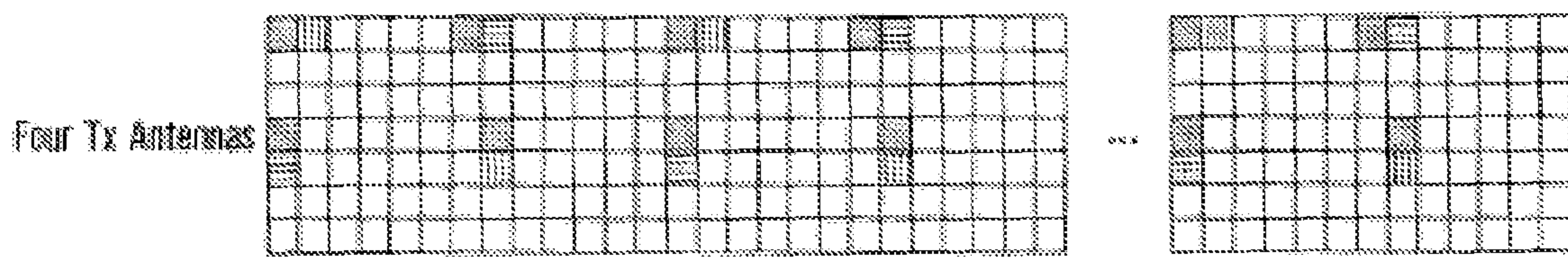


Figure 12B

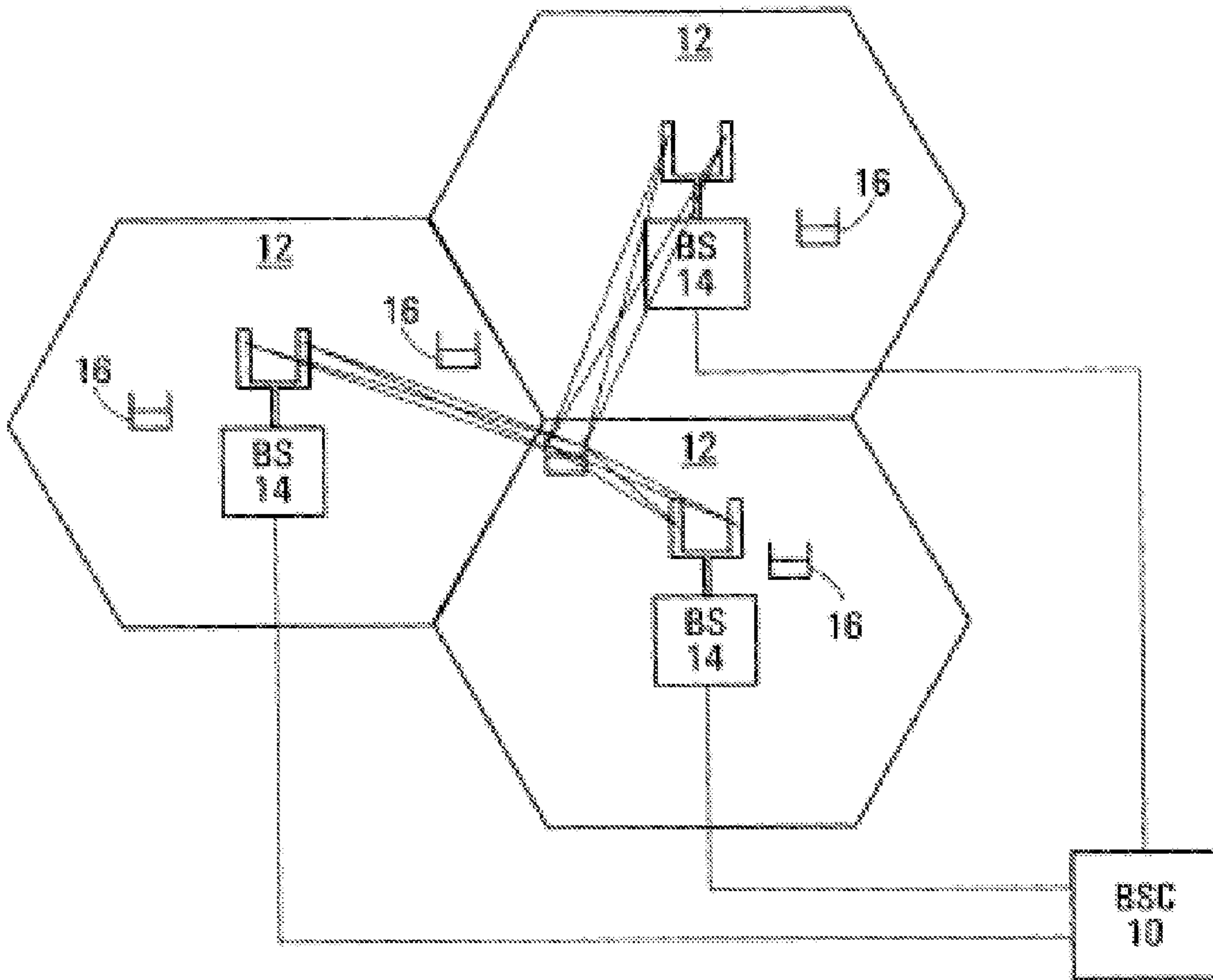


Figure 13

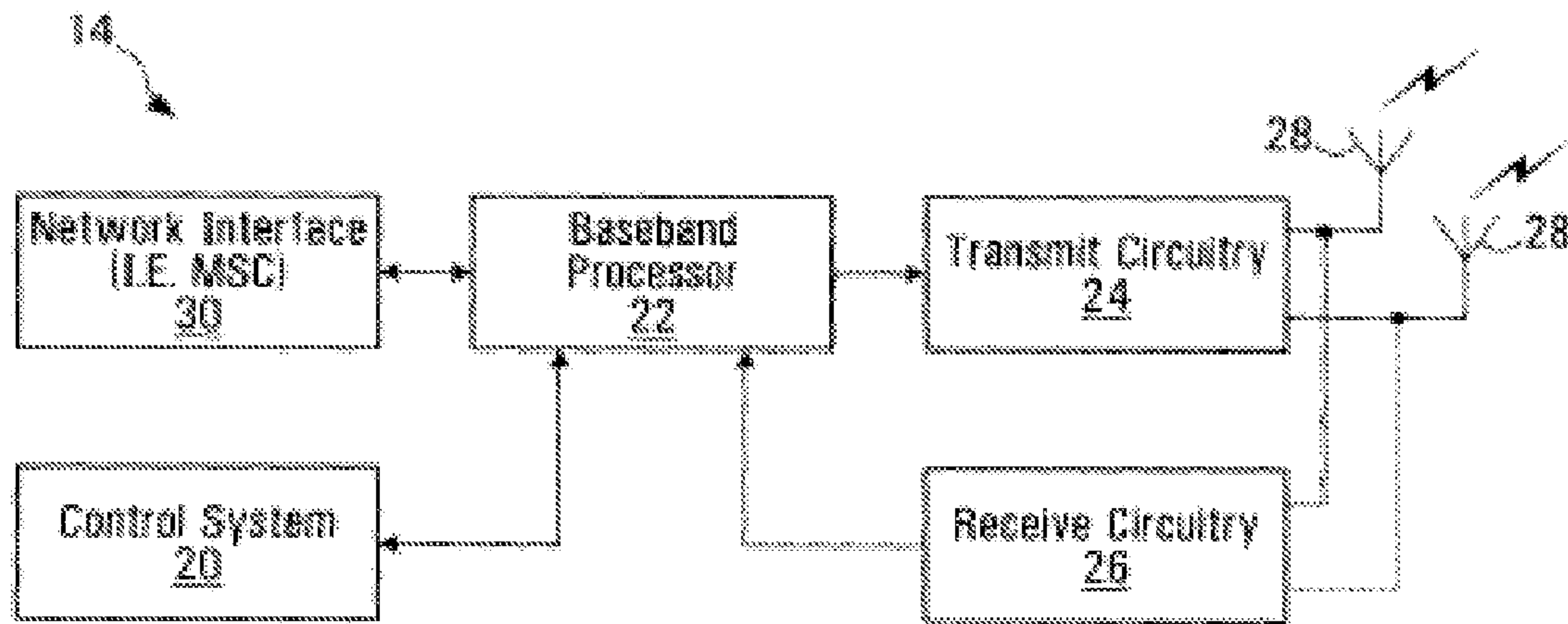


Figure 14

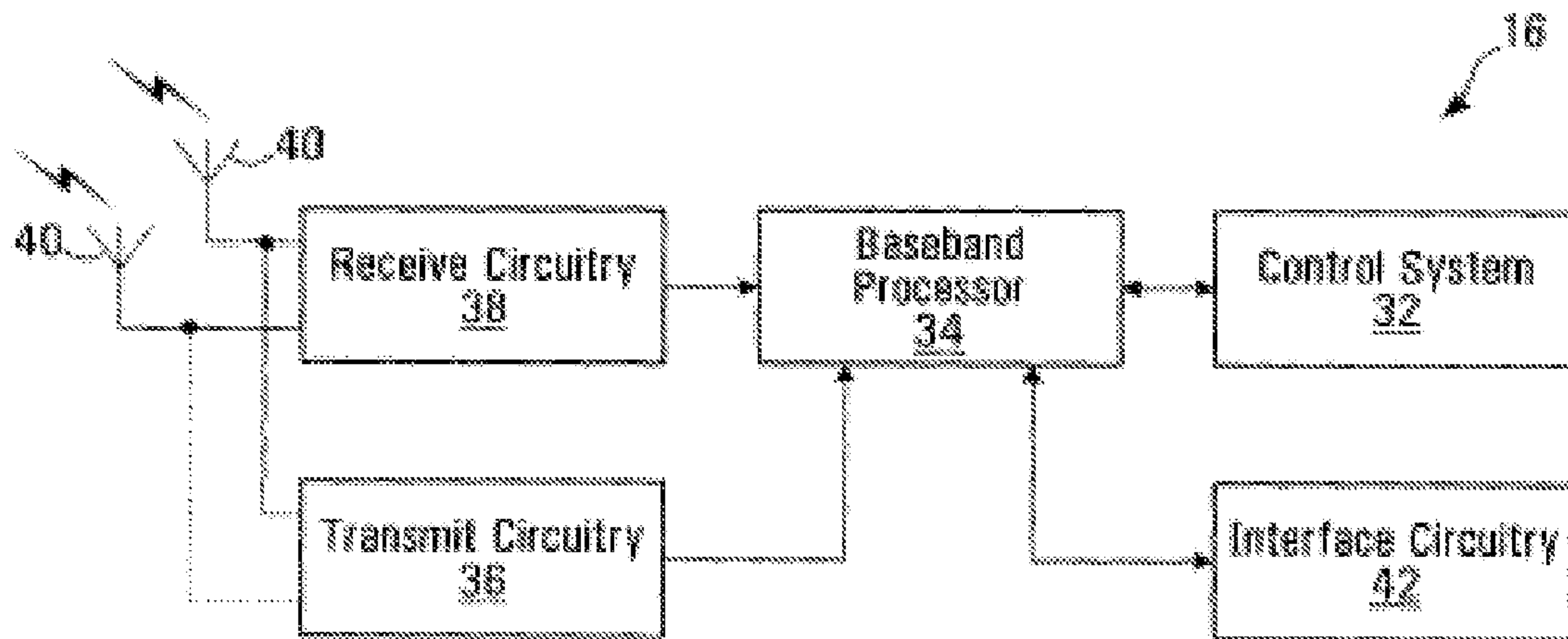


Figure 15

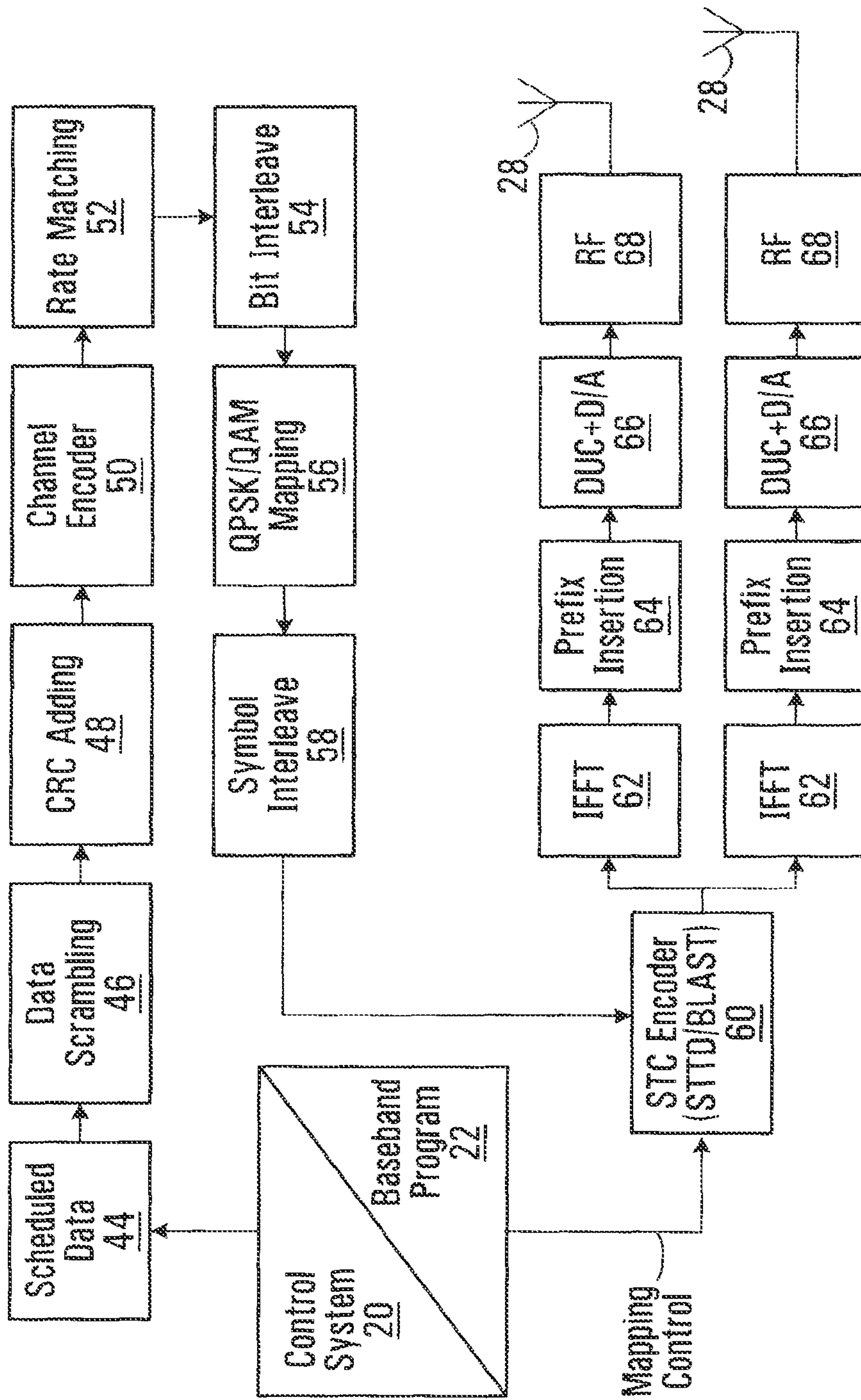


FIG. 16

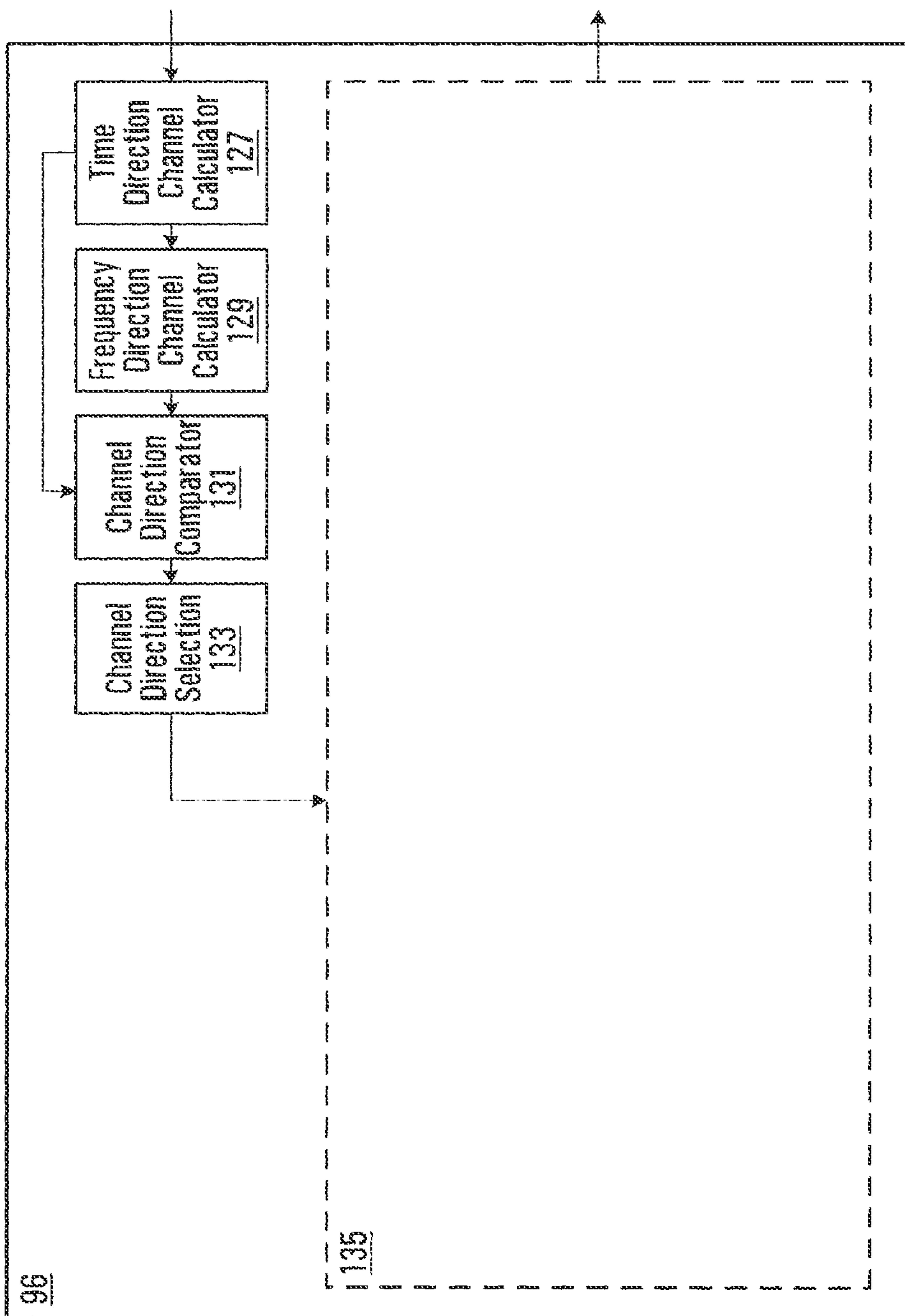


FIG. 18

ADAPTIVE TWO-DIMENSIONAL CHANNEL INTERPOLATION

PRIORITY CLAIM

This application is a continuation of and claims the benefit of priority from U.S. patent application Ser. No. 13/665,982, entitled "Adaptive Two-Dimensional Channel Interpolation" and filed on Nov. 1, 2012, which is a continuation of and claims the benefit of priority from U.S. patent application Ser. No. 12/064,566, entitled "Adaptive Two-Dimensional Channel Interpolation" and filed on Sep. 4, 2008 (issued as U.S. Pat. No. 8,331,465 on Dec. 11, 2012), which is a National Stage of and claims the benefit of priority from PCT/CA2006/001380, entitled "Adaptive Two-Dimensional Channel Interpolation" and filed on Aug. 22, 2006, which claims the benefit of priority from U.S. Provisional Patent Application Nos. 60/722,744, and filed on Sep. 30, 2005, and 60/710,527, filed on Aug. 23, 2005, all of which are fully incorporated herein by reference for all purposes.

BACKGROUND

1. Field of the Application

This invention relates to Orthogonal Frequency Division Multiplexing (OFDM) communication systems, and more particularly to channel interpolation with the use of pilot symbols.

2. Background of the Disclosure

In wireless communication systems that employ OFDM, a transmitter transmits data to a receiver using many sub-carriers in parallel. The frequencies of the sub-carriers are orthogonal.

Channel estimation in OFDM is usually performed with the aid of known pilot symbols which are sparsely inserted in a stream of data symbols. The attenuation of the pilot symbols is measured and the attenuations of the data symbols in between these pilot symbols are then estimated/interpolated.

Pilot symbols are overhead, and should be as few in number as possible in order to maximize the transmission rate of data symbols. It is desirable that channel estimation in OFDM be as accurate as possible without sacrificing bandwidth.

SUMMARY

In one embodiment, there is provided a method comprising receiving channel estimates for four pilot symbols in a scattered pilot pattern in time-frequency; calculating the channel response for the pilot symbols in both a first direction and a second direction; determining whether the channel changes more slowly in one direction than the other; and interpolating in the direction of slower channel change.

In some embodiments, the method of further comprises interpolating in the direction of faster channel change.

In some embodiments, the step of interpolating in the direction of faster channel change is performed using the result from the step of interpolating in the direction of slower channel change.

In some embodiments, the channel changes are calculated by performing an inner products operation.

In some embodiments, the first direction is a time direction and the second direction is a frequency direction.

In some embodiments, the first direction is a frequency direction and the second direction is a time direction.

In some embodiments, the scattered pilot pattern is a regular diamond lattice.

In some embodiments, the scattered pilot pattern is an irregular diamond lattice.

In some embodiments, the scattered pilot pattern is kite shaped.

5 In another embodiment, there is provided an OFDM receiver comprising: one or more receive antennas; the OFDM transmitter being adapted to receive channel estimates for four pilot symbols in a scattered pilot pattern in time-frequency, calculate channel changes for the pilot symbols in a first direction and a second direction, and interpolate
10 in the direction of slower channel change.

In yet another embodiment, there is provided a method of interpolation using a set of four pilot symbols in a scattered pilot pattern in time-frequency wherein the set of four pilot symbols comprise first and second pilot symbols on a common sub-carrier frequency, spaced in time, and third and fourth pilot symbols transmitted on different sub-carriers on a common OFDM symbol period, the method comprising:
15 determining a first channel change between the first and second pilot symbols; determining a second channel change between the third and fourth pilot symbols; determining which of the first and second channel change is slower; if the first channel change is slower, interpolating using the first and second pilot symbols to generate a channel estimate for the
20 common sub-carrier frequency at the common OFDM symbol period, and then using the channel estimate in subsequent interpolations to determine other channel estimates; and if the second channel change is slower, interpolating using the third and fourth pilot symbols to generate a channel estimate for the
25 common sub-carrier frequency at the common OFDM symbol period, and then using the channel estimate in subsequent interpolations to determine other channel estimates.

In yet another embodiment, a method of inserting pilot symbols into OFDM sub-frames for transmission by a plurality of transmitting antenna, the OFDM sub-frames having a time domain and a frequency domain, each OFDM sub-frame comprising a plurality of OFDM symbols, the method comprising: for each sub-frame, defining a set of at least two OFDM symbols none of which are consecutive that are to
35 contain pilot symbols; at each antenna, inserting pilot symbols in each of the set of at least two OFDM symbols in a scattered pattern that does not interfere with the scattered pattern inserted by any other antenna.

Other aspects and features of the present invention will
45 become apparent to those ordinarily skilled in the art upon review of the following description of specific embodiments of the invention in conjunction with the accompanying figures. TBD

BRIEF DESCRIPTION OF THE DRAWINGS

Preferred embodiments of the invention will now be described with reference to the attached drawings in which:

55 FIG. 1 is a diagram of a single antenna perfect diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 2 is a flowchart of a method of performing adaptive interpolation in accordance with one embodiment of the present invention;

60 FIG. 3 presents simulation results for one example of adaptive interpolation;

FIG. 4A is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can used in accordance with an embodiment of the present invention;

65 FIG. 4B is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can used in accordance with an embodiment of the present invention;

FIG. 5A is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 5B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 5C is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 5D is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 6 is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 7A is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 7B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 7C is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 7D is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 8 is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 9A is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 9B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 9C is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 9D is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 10A is a diagram of a one antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 10B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 11A is a diagram of a one antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 11B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 12A is a diagram of a one antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 12B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention;

FIG. 13 is a block diagram of a cellular communication system;

FIG. 14 is a block diagram of an example base station that might be used to implement some embodiments of the present invention;

FIG. 15 is a block diagram of an example wireless terminal that might be used to implement some embodiments of the present invention;

FIG. 16 is a block diagram of a logical breakdown of an example OFDM transmitter architecture that might be used to implement some embodiments of the present invention;

FIG. 17 is a block diagram of a logical breakdown of an example OFDM receiver architecture that might be used to implement some embodiments of the present invention; and

FIG. 18 is a block diagram of one embodiment of the present invention. TBD

DETAILED DESCRIPTION

Channel estimation in OFDM is usually performed with the aid of pilot symbols. More particularly, at an OFDM transmitter, known pilot symbols are periodically transmitted along with data symbols. The pilot symbols are typically spaced in time and frequency.

The variations in phase and amplitude resulting from propagation across an OFDM channel are referred to as the channel response. The channel response is usually frequency and time dependent. If an OFDM receiver can determine the channel response, the received signal can be corrected to compensate for the channel degradation. The determination of the channel response is called channel estimation. The transmission of known pilot symbols along with data symbols allows the receiver to carry out channel estimation.

When a receiver receives an OFDM signal, the receiver compares the received value of the pilot symbols with the known transmitted value of the pilot symbols to estimate the channel response.

Since the channel response can vary with time and with frequency, the pilot symbols are scattered amongst the data symbols to provide a range of channel responses over time and frequency. The set of frequencies and times at which pilot symbols are inserted is referred to as a pilot pattern. In some cases, the pilot pattern is a diagonal-shaped lattice, either regular or irregular.

FIG. 1 is an example pilot pattern which can be used in accordance with one embodiment of the present invention. Pilot and data symbols are spread over an OFDM sub-frame in a time direction **120** and a frequency direction **122**. Most symbols within the OFDM sub-frame are data symbols **124**. Pilot symbols **126** are inserted in a diamond lattice pattern. In the illustrated example, the diamond lattice pattern in which each encoded pilot symbols are inserted within the OFDM sub-frame is a perfect diamond lattice pattern as illustrated by pilot symbols h_1 , h_2 , h_3 and h_4 .

A two dimensional interpolator is used to estimate the channel response at point h which is between four points of known channel response, i.e. pilot symbols h_1 , h_2 , h_3 and h_4 . Point h can then be used as an additional point from which the receiver can carry out channel estimation. The use of point h would, of course, not add any overhead to the OFDM signal.

The channel interpolation scheme is adaptive, i.e. it is a scheme which can adapt to varying conditions in the

$$h(i,j)=w_1(i,j)h_1+w_2(i,j)h_2+w_3(i,j)h_3+w_4(i,j)h_4$$

channel. The following formula presents a particular example of adaptive two-dimensional (time direction and frequency direction) interpolator to calculate point h :

$$\text{where } w_1(i,j)+w_2(i,j)+w_3(i,j)+w_4(i,j)=1$$

In this case, the two dimensional channel interpolation can be viewed as the sum of two one-dimensional interpolations.

The weights $w_k(i,j)$ may be adapted to coherence time and frequency of the channel. In some embodiments, if the chan-

5

nel coherence is less in the time direction than it is in the frequency direction, then h would be calculated using the following formula:

$$h(i,j)=w_1(i,j)h_1+w_2(i,j)h_2+w_3(i,j)h_3+w_4(i,j)h_4$$

where

$$\begin{aligned} w_3(i,j) &= 0, \\ w_4(i,j) &= 0, \text{ and} \\ w_1(i,j) + w_2(i,j) &= 1. \end{aligned}$$

Alternatively, if the channel coherence is greater in the time direction than it is in the frequency direction, then h would be calculated using the following formula:

$$h(i,j)=w_1(i,j)h_1+w_2(i,j)h_2+w_3(i,j)h_3+w_4(i,j)h_4$$

where

$$\begin{aligned} w_1(i,j) &= 0, \\ w_2(i,j) &= 0, \text{ and} \\ w_3(i,j) + w_4(i,j) &= 1. \end{aligned}$$

In another embodiment, the weights in both directions (time and frequency) are adaptively changed according to the channel coherence in the time and frequency directions as follows:

$$h(i,j)=c_{time}w_1(i,j)h_1+c_{time}w_2(i,j)h_2+c_{freq}w_3(i,j)h_3+c_{freq}w_4(i,j)h_4$$

$$c_{time}+c_{freq}=1$$

$$w_1(i,j)+w_2(i,j)+w_3(i,j)+w_4(i,j)=1$$

According to one embodiment, the sequence of interpolation is adapted to the coherence of the channel.

One way to achieve adaptive interpolation is to divide the interpolation into two one-dimensional steps as shown in the flowchart illustrated in FIG. 2:

- i. at step **210**, calculate the channel changes in both time and frequency directions and determine in which direction the channel changes faster;
- ii. at step **220**, perform one-dimensional interpolation in the direction with slower channel change to calculate h ; and
- iii. at step **230**, using h , perform one-dimensional interpolation in the direction with faster channel change.

The method of adaptive interpolation set out above takes advantage of the fact that interpolated results from the direction of larger coherence time/frequency is more reliable, and hence is interpolated first. The calculation of h will effectively increase the density of pilot symbols in the direction of faster change thereby improving channel estimation without increasing overhead. As such, the results of the first interpolating step can then be used to assist the interpolation in the dimension of smaller coherence time/frequency.

In general, there are at least three ways to evaluate the channel change between two pilots, including:

- i. Euclidean distance. One problem with Euclidean distance, however, is that it is not sensitive to phase change;
- ii. Phase change. One problem with phase change, however, is computation complexity; and
- iii. Amplitude change. One problem with amplitude change, however, is that it is insensitive to phase change.

In light of these drawbacks a way to measure channel change so as to take both amplitude change and phase change into account, while at the same time keeping the computation complexity to a minimum, is desirable. According to an embodiment of the invention, therefore, a way of using the inner products of the two pilot assisted channel estimates as a measurement of channel change is shown below.

$$\Lambda_{freq}\langle h_1, h_2 \rangle = |h_1||h_2|\cos(\theta_{1,2})$$

6

Λ_{time} denotes channel change in the time direction.

Λ_{freq} denotes channel change in the frequency direction.

The term " $\langle h_n, h_m \rangle$ " denotes the inner product of h_n and h_m .

The term " $|h_n|$ " denotes the magnitude of the vector h_n . If

$$h_n = a + bi \text{ then } |h_n| = \text{sqr}(a^2 + b^2).$$

The term " $\cos(\theta_{1,2})$ " denotes the cosine of the difference in angle between h_n and h_m : $\cos(\theta_{n,m}) = \cos(\theta_n - \theta_m)$. If $h_n = a + bi$ then θ_n can be calculated as $\theta_n = \tan^{-1}(b/a)$.

The vector h_n can be represented as $h_n = |h_n|e^{i\theta_n}$, or as $h_n = a + bi$, where

$$a = |h_n|\cos(\theta_n), \text{ and } b = |h_n|\sin(\theta_n).$$

When the amplitude changes linearly between the two channel estimates, the maximum Λ is achieved when

$$|h_1| = |h_2| \text{ in frequency and } |h_3| = |h_4| \text{ in time.}$$

Hence the more the channel changes, the smaller the Λ , regardless whether this change is in amplitude or phase. The inner product is able to solve phase ambiguity. When $|\theta| > \pi/2$ (which rarely occurs), $\cos(\Lambda\theta)$ becomes negative, and hence smaller. An inner product may then be computed, which requires two real multiplications and one real addition, and the result is therefore a real number.

Referring again to FIG. 1, what follows is an example of the adaptive interpolation method.

Assume:

$$\begin{aligned} h_1 &= 0.4423 - 1.0968i, \\ h_2 &= -0.0051 - 0.1484i, \\ h_3 &= 0.1258 - 0.3413i, \text{ and} \\ h_4 &= 0.3958 - 0.5883i. \end{aligned}$$

The central point, known from a simulation, has the value of $h = 0.2859 - 0.4224i$.

The inner product is then calculated as follows:

$$\langle h_1, h_2 \rangle = 0.1605$$

$$\langle h_3, h_4 \rangle = 0.2506$$

where $\langle h_1, h_2 \rangle$ denotes the inner product of h_1 and h_2 .

If $h_1 = a_1 + ib_1$ and $h_2 = a_2 + ib_2$ then the inner product can be calculated as

$$\langle h_1, h_2 \rangle = a_1a_2 + b_1b_2.$$

Alternatively, $\langle h_1, h_2 \rangle = |h_1||h_2|\cos(\theta_2 - \theta_1)$.

Since $\langle h_1, h_2 \rangle < \langle h_3, h_4 \rangle$, the channel changes faster in the h_1/h_2 direction. h is then estimated in both the frequency and time directions:

$$\tilde{h}_{h_1, h_2} = 0.5(h_1 + h_2) = 0.2186 - 0.6226i$$

$$\tilde{h}_{h_3, h_4} = 0.5(h_3 + h_4) = 0.2608 - 0.4648i$$

Compared with the known h , obviously \tilde{h}_{h_3, h_4} provides a better estimate \tilde{h}_{h_1, h_2} ; hence \tilde{h}_{h_3, h_4} can be used to improve the channel interpolation quality in the h_1/h_2 direction.

Note that there is no requirement that h be the middle point equidistant from h_1 , h_2 , h_3 and h_4 .

In the example above, the interpolation sequence was determined to be:

- i. interpolate between the two pilots in the time direction first to calculate h , and
- ii. use h and/or one or both of the two pilots to interpolate in the frequency direction.

Of course, if the initial calculation used to determine which channel direction changes faster determines that the h_3/h_4 direction changes faster, then the interpolation sequence will be:

- i. interpolate between the two pilots in the frequency direction first to calculate h , and
- ii. use h and/or one or both of the two pilots to interpolate in the time direction.

Once h is calculated, any one of a number of conventional channel estimation techniques can be used. Such channel estimation techniques typically consist of two steps. First, the attenuations at the pilot positions are measured. This measurement is calculated using the formula:

$$H(n, k) = \frac{Y(n, k)}{X(n, k)}$$

where $X(n, k)$ is the known pilot symbol, and $Y(n, k)$ is the received pilot symbol.

These measurements are then used to estimate (interpolate) the attenuations of the data symbols in the second step. Persons skilled in the art will appreciate that such channel estimation techniques include, but are not limited to, linear interpolation, second order interpolation, maximum likelihood (least square in time domain), linear minimum square error and others.

In another embodiment, a “majority vote” is used to determine the interpolation sequence for all the “diamonds” across the frequency domain. This means that there are several calculations performed along the frequency direction for the channel change. Some results will indicate there is more change in time, while other results indicate there is more change in frequency. The “majority vote” option means the choice whether to interpolate first in the time direction or the frequency direction is arrived at by assessing the majority of the results. For example, if the majority of the results indicate that the channel changes faster in the time direction, then interpolation is first performed in the frequency direction, and then in the time direction. If the majority of the results indicate that the channel changes faster in the frequency direction, then interpolation is first performed in the time direction, and is then performed in the frequency direction.

In accordance with an embodiment of the invention, FIG. 3 presents simulation results for the adaptive interpolation method described above. The results show the benefit of adaptive interpolation when channel changes slower in the time direction when UE speed is low, and slower in the frequency direction when UE speed is high. The curve of “ideal channel” is of the case with clean known channel, i.e. with no interpolation loss and additive noise. As shown this approach recoups most of the interpolation loss. The results were obtained with the majority vote option described above.

It is not necessary that there be a regular diamond shaped pilot pattern in order to use the adaptive interpolation method described above. For example, an irregular diamond shaped pilot pattern can be used in accordance with other embodiments of the present invention, such as the scattered pilot patterns shown in FIGS. 4A to 11. In FIGS. 4A to 11, the number of OFDM symbols per Transmission Time Interval (TTI) is odd instead of even. In some embodiments, the scattered pilot patterns can be generated by more than one antenna such as is shown in FIGS. 5, 7, 9, 10, 11 and 12.

In general, the adaptive interpolation method works with all “staggered” pilot patterns which describes all shapes other than a square, which does not work. A perfect diamond shape, which is the most favorable shape, is a special case of a staggered pilot pattern. Another example of a pattern which would work is a “kite” pattern where the pilots are spread further apart in one direction than the other.

More generally, in FIGS. 4A to 11, in each sub-frame, pilots are transmitted by part of the sub-carriers in at least two non-contiguous OFDM symbols by at least one transmit antenna. The pilot sub-carriers in the first OFDM symbol and

the second OFDM symbol are staggered in the frequency domain. In FIGS. 5A, 5D, 7A, 7D, 9A and 9D, pilot symbols from all transmit antennas are transmitted through the same non-contiguous OFDM symbols. This arrangement will save the terminal power since only two OFDM symbols are coded to obtain the channel information.

FIG. 4A is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention. The overhead associated with this pilot pattern is 1/28 per antenna. Pilot and data symbols are spread over an OFDM sub-frame in a time direction 420 and a frequency direction 422. Most symbols within the OFDM sub-frame are data symbols 424. Pilot symbols 426 are inserted in an irregular diamond lattice pattern. In this embodiment, an OFDM sub-frame comprises eight sub-carriers 428 and seven OFDM symbols 430.

As with the scattered pilot pattern in FIG. 1, there is first performed a calculation of the channel changes in both the time direction and the frequency direction and a comparison is made as to which direction the channel changes faster. One-dimensional interpolation is then performed in the direction with slower channel change. One-dimensional interpolation is then performed in the direction with faster channel change.

FIG. 4B is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention. Though similar to FIG. 4A, in this case one of the pilots in each diamond lattice is offset by one OFDM symbol position. Thus, the adaptive interpolation method does not require that the scattered pilots line up in either or both of the time direction and the frequency direction. In the case of staggered pilot patterns where the pilots do not line up in either the time direction, the frequency direction, or both, it is more accurate to refer to the “ h_1/h_2 direction” and the “ h_3/h_4 direction” rather than the time direction and the frequency direction.

FIG. 5A is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention. The overhead associated with this scattered pilot pattern is 1/28 per antenna. In this embodiment, an OFDM frame comprises eight sub-carriers 528 and seven OFDM symbols 530.

Pilot and data symbols are spread over an OFDM frame in a time direction 420 and a frequency direction 522. Most symbols within the OFDM frame are data symbols 524. Pilot symbols 526 are inserted in an irregular diamond lattice pattern.

As with the scattered pilot pattern in FIG. 1, there is first performed a calculation of the channel changes in both the time direction and the frequency direction and a comparison is made as to which direction the channel changes faster. One-dimensional interpolation is then performed in the direction with slower channel change. Using these measurements, one-dimensional interpolation is then performed in the direction with faster channel change.

FIGS. 5B, 5C and 5D are three other examples of scattered pilot patterns which can be generated according to this embodiment.

FIG. 6 is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 7A is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 7B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 7C is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 7D is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 8 is a diagram of a single antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 9A is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 9B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 9C is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 9D is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 10A is a diagram of a one antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 10B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 11A is a diagram of a one antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 11B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 12A is a diagram of a one antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

FIG. 12B is a diagram of a four antenna irregular diamond lattice scattered pilot pattern which can be used in accordance with an embodiment of the present invention.

For the purposes of providing context for embodiments of the invention for use in a communication system, FIGS. 13-17 will now be described. As will be described in more detail below, the method of the present invention can, in one embodiment, be implemented through means of the channel estimation logic of a conventional OFDM receiver (see channel estimation 96 in FIG. 17).

FIG. 13 shows a base station controller (BSC) 10 which controls wireless communications within multiple cells 12, which cells are served by corresponding base stations (BS) 14. In general, each base station 14 facilitates communications using OFDM with mobile and/or wireless terminals 16, which are within the cell 12 associated with the corresponding base station 14. The movement of the mobile terminals 16 in relation to the base stations 14 results in significant fluctuation in channel conditions. As illustrated, the base stations 14 and mobile terminals 16 may include multiple antennas to provide spatial diversity for communications.

A high level overview of the mobile terminals 16 and base stations 14 upon which aspects of the present invention may be implemented is provided prior to delving into the structural and functional details of the preferred embodiments. With reference to FIG. 14, a base station 14 is illustrated. The base station 14 generally includes a control system 20, a baseband processor 22, transmit circuitry 24, receive circuitry 26, multiple antennas 28, and a network interface 30. The receive circuitry 26 receives radio frequency signals bearing information from one or more remote transmitters provided by

mobile terminals 16 (illustrated in FIG. 13). A low noise amplifier and a filter (not shown) may cooperate to amplify and remove broadband interference from the signal for processing. Downconversion and digitization circuitry (not shown) will then downconvert the filtered, received signal to an intermediate or baseband frequency signal, which is then digitized into one or more digital streams.

The baseband processor 22 processes the digitized received signal to extract the information or data bits conveyed in the received signal. This processing typically comprises demodulation, decoding, and error correction operations. As such, the baseband processor 22 is generally implemented in one or more digital signal processors (DSPs) or application-specific integrated circuits (ASICs). The received information is then sent across a wireless network via the network interface 30 or transmitted to another mobile terminal 16 serviced by the base station 14.

On the transmit side, the baseband processor 22 receives digitized data, which may represent voice, data, or control information, from the network interface 30 under the control of control system 20, and encodes the data for transmission. The encoded data is output to the transmit circuitry 24, where it is modulated by a carrier signal having a desired transmit frequency or frequencies. A power amplifier (not shown) will amplify the modulated carrier signal to a level appropriate for transmission, and deliver the modulated carrier signal to the antennas 28 through a matching network (not shown). Various modulation and processing techniques available to those skilled in the art are used for signal transmission between the base station and the mobile terminal.

With reference to FIG. 15, a mobile terminal 16 configured according to one embodiment of the present invention is illustrated. Similarly to the base station 14, the mobile terminal 16 will include a control system 32, a baseband processor 34, transmit circuitry 36, receive circuitry 38, multiple antennas 40, and user interface circuitry 42. The receive circuitry 38 receives radio frequency signals bearing information from one or more base stations 14. A low noise amplifier and a filter (not shown) may cooperate to amplify and remove broadband interference from the signal for processing. Downconversion and digitization circuitry (not shown) will then downconvert the filtered, received signal to an intermediate or baseband frequency signal, which is then digitized into one or more digital streams.

The baseband processor 34 processes the digitized received signal to extract the information or data bits conveyed in the received signal. This processing typically comprises demodulation, decoding, and error correction operations. The baseband processor 34 is generally implemented in one or more digital signal processors (DSPs) and application specific integrated circuits (ASICs).

For transmission, the baseband processor 34 receives digitized data, which may represent voice, data, or control information, from the control system 32, which it encodes for transmission. The encoded data is output to the transmit circuitry 36, where it is used by a modulator to modulate a carrier signal that is at a desired transmit frequency or frequencies. A power amplifier (not shown) will amplify the modulated carrier signal to a level appropriate for transmission, and deliver the modulated carrier signal to the antennas 40 through a matching network (not shown). Various modulation and processing techniques available to those skilled in the art are used for signal transmission between the mobile terminal and the base station.

In OFDM modulation, the transmission band is divided into multiple, orthogonal carrier waves. Each carrier wave is modulated according to the digital data to be transmitted.

Because OFDM divides the transmission band into multiple carriers, the bandwidth per carrier decreases and the modulation time per carrier increases. Since the multiple carriers are transmitted in parallel, the transmission rate for the digital data, or symbols, on any given carrier is lower than when a single carrier is used.

OFDM modulation utilizes the performance of an Inverse Fast Fourier Transform (IFFT) on the information to be transmitted. For demodulation, the performance of a Fast Fourier Transform (FFT) on the received signal recovers the transmitted information. In practice, the IFFT and FFT are provided by digital signal processing carrying out an Inverse Discrete Fourier Transform (IDFT) and Discrete Fourier Transform (DFT), respectively. Accordingly, the characterizing feature of OFDM modulation is that orthogonal carrier waves are generated for multiple bands within a transmission channel. The modulated signals are digital signals having a relatively low transmission rate and capable of staying within their respective bands. The individual carrier waves are not modulated directly by the digital signals. Instead, all carrier waves are modulated at once by IFFT processing.

In operation, OFDM is preferably used for at least down-link transmission from the base stations **14** to the mobile terminals **16**. Each base station **14** is equipped with “n” transmit antennas **28**, and each mobile terminal **16** is equipped with “m” receive antennas **40**. Notably, the respective antennas can be used for reception and transmission using appropriate duplexers or switches and are so labeled only for clarity.

With reference to FIG. **16**, a logical OFDM transmission architecture will be described. Initially, the base station controller **10** will send data to be transmitted to various mobile terminals **16** to the base station **14**. The base station **14** may use the channel quality indicators (CQIs) associated with the mobile terminals to schedule the data for transmission as well as select appropriate coding and modulation for transmitting the scheduled data. The CQIs may be directly from the mobile terminals **16** or determined at the base station **14** based on information provided by the mobile terminals **16**. In either case, the CQI for each mobile terminal **16** is a function of the degree to which the channel amplitude (or response) varies across the OFDM frequency band.

Scheduled data **44**, which is a stream of bits, is scrambled in a manner reducing the peak-to-average power ratio associated with the data using data scrambling logic **46**. A cyclic redundancy check (CRC) for the scrambled data is determined and appended to the scrambled data using CRC adding logic **48**. Next, channel coding is performed using channel encoder logic **50** to effectively add redundancy to the data to facilitate recovery and error correction at the mobile terminal **16**. Again, the channel coding for a particular mobile terminal **16** is based on the CQI. In some implementations, the channel encoder logic **50** uses known Turbo encoding techniques. The encoded data is then processed by rate matching logic **52** to compensate for the data expansion associated with encoding.

Bit interleaver logic **54** systematically reorders the bits in the encoded data to minimize the loss of consecutive data bits. The resultant data bits are systematically mapped into corresponding symbols depending on the chosen baseband modulation by mapping logic **56**. Preferably, Quadrature Amplitude Modulation (QAM) or Quadrature Phase Shift Key (QPSK) modulation is used. The degree of modulation is preferably chosen based on the CQI for the particular mobile terminal. The symbols may be systematically reordered to further bolster the immunity of the transmitted signal to periodic data loss caused by frequency selective fading using symbol interleaver logic **58**.

At this point, groups of bits have been mapped into symbols representing locations in an amplitude and phase constellation. When spatial diversity is desired, blocks of symbols are then processed by space-time block code (STC) encoder logic **60**, which modifies the symbols in a fashion making the transmitted signals more resistant to interference and more readily decoded at a mobile terminal **16**. The STC encoder logic **60** will process the incoming symbols and provide “n” outputs corresponding to the number of transmit antennas **28** for the base station **14**. The control system **20** and/or baseband processor **22** as described above with respect to FIG. **14** will provide a mapping control signal to control STC encoding. At this point, assume the symbols for the “n” outputs are representative of the data to be transmitted and capable of being recovered by the mobile terminal **16**.

For the present example, assume the base station **14** has two antennas **28** (n=2) and the STC encoder logic **60** provides two output streams of symbols. Accordingly, each of the symbol streams output by the STC encoder logic **60** is sent to a corresponding IFFT processor **62**, illustrated separately for ease of understanding. Those skilled in the art will recognize that one or more processors may be used to provide such digital signal processing, alone or in combination with other processing described herein. The IFFT processors **62** will preferably operate on the respective symbols to provide an inverse Fourier Transform. The output of the IFFT processors **62** provides symbols in the time domain. The time domain symbols are grouped into frames, which are associated with a prefix by prefix insertion logic **64**. Each of the resultant signals is up-converted in the digital domain to an intermediate frequency and converted to an analog signal via the corresponding digital up-conversion (DUC) and digital-to-analog (D/A) conversion circuitry **66**. The resultant (analog) signals are then simultaneously modulated at the desired RF frequency, amplified, and transmitted via the RF circuitry **68** and antennas **28**. Notably, pilot signals known by the intended mobile terminal **16** are scattered among the sub-carriers. The mobile terminal **16**, which is discussed in detail below, will use the pilot signals for channel estimation.

Reference is now made to FIG. **17** to illustrate reception of the transmitted signals by a mobile terminal **16**. Upon arrival of the transmitted signals at each of the antennas **40** of the mobile terminal **16**, the respective signals are demodulated and amplified by corresponding RF circuitry **70**. For the sake of conciseness and clarity, only one of the two receive paths is described and illustrated in detail. Analog-to-digital (A/D) converter and down-conversion circuitry **72** digitizes and downconverts the analog signal for digital processing. The resultant digitized signal may be used by automatic gain control circuitry (AGC) **74** to control the gain of the amplifiers in the RF circuitry **70** based on the received signal level.

Initially, the digitized signal is provided to synchronization logic **76**, which includes coarse synchronization logic **78**, which buffers several OFDM symbols and calculates an auto-correlation between the two successive OFDM symbols. A resultant time index corresponding to the maximum of the correlation result determines a fine synchronization search window, which is used by fine synchronization logic **80** to determine a precise framing starting position based on the headers. The output of the fine synchronization logic **80** facilitates frame acquisition by frame alignment logic **84**. Proper framing alignment is important so that subsequent FFT processing provides an accurate conversion from the time domain to the frequency domain. The fine synchronization algorithm is based on the correlation between the received pilot signals carried by the headers and a local copy of the known pilot data. Once frame alignment acquisition

occurs, the prefix of the OFDM symbol is removed with prefix removal logic **86** and resultant samples are sent to frequency offset correction logic **88**, which compensates for the system frequency offset caused by the unmatched local oscillators in the transmitter and the receiver. Preferably, the synchronization logic **76** includes frequency offset and clock estimation logic **82**, which is based on the headers to help estimate such effects on the transmitted signal and provide those estimations to the correction logic **88** to properly process OFDM symbols.

At this point, the OFDM symbols in the time domain are ready for conversion to the frequency domain using FFT processing logic **90**. The results are frequency domain symbols, which are sent to processing logic **92**. The processing logic **92** extracts the scattered pilot signal using scattered pilot extraction logic **94**, determines a channel estimate based on the extracted pilot signal using channel estimation logic **96**, and provides channel responses for all sub-carriers using channel reconstruction logic **98**. In order to determine a channel response for each of the sub-carriers, the pilot signal is essentially multiple pilot symbols that are scattered among the data symbols throughout the OFDM sub-carriers in a known pattern in both time and frequency. Examples of scattering of pilot symbols among available sub-carriers over a given time and frequency plot in an OFDM environment are found in PCT Patent Application No. PCT/CA2005/000387 filed Mar. 15, 2005 assigned to the same assignee of the present application. Continuing with FIG. **17**, the processing logic compares the received pilot symbols with the pilot symbols that are expected in certain sub-carriers at certain times to determine a channel response for the sub-carriers in which pilot symbols were transmitted. The results are interpolated to estimate a channel response for most, if not all, of the remaining sub-carriers for which pilot symbols were not provided. The actual and interpolated channel responses are used to estimate an overall channel response, which includes the channel responses for most, if not all, of the sub-carriers in the OFDM channel.

The frequency domain symbols and channel reconstruction information, which are derived from the channel responses for each receive path are provided to an STC decoder **100**, which provides STC decoding on both received paths to recover the transmitted symbols. The channel reconstruction information provides equalization information to the STC decoder **100** sufficient to remove the effects of the transmission channel when processing the respective frequency domain symbols.

The recovered symbols are placed back in order using symbol de-interleaver logic **102**, which corresponds to the symbol interleaver logic **58** of the transmitter. The de-interleaved symbols are then demodulated or de-mapped to a corresponding bitstream using de-mapping logic **104**. The bits are then de-interleaved using bit de-interleaver logic **106**, which corresponds to the bit interleaver logic **54** of the transmitter architecture. The de-interleaved bits are then processed by rate de-matching logic **108** and presented to channel decoder logic **110** to recover the initially scrambled data and the CRC checksum. Accordingly, CRC logic **112** removes the CRC checksum, checks the scrambled data in traditional fashion, and provides it to the de-scrambling logic **114** for de-scrambling using the known base station de-scrambling code to recover the originally transmitted data **116**.

In parallel to recovering the data **116**, a CQI, or at least information sufficient to create a CQI at the base station **14**, is determined and transmitted to the base station **14**. As noted above, the CQI may be a function of the carrier-to-interference ratio (CR), as well as the degree to which the channel

response varies across the various sub-carriers in the OFDM frequency band. The channel gain for each sub-carrier in the OFDM frequency band being used to transmit information is compared relative to one another to determine the degree to which the channel gain varies across the OFDM frequency band. Although numerous techniques are available to measure the degree of variation, one technique is to calculate the standard deviation of the channel gain for each sub-carrier throughout the OFDM frequency band being used to transmit data.

FIG. **18** is a block diagram of one embodiment of the present invention. In this embodiment, the present invention is shown being implemented within channel estimation logic **96** of FIG. **17** with the conventional aspects of channel estimation logic **96** being shown in dotted outline for ease of reference. Persons skilled in the art will appreciate that the present invention could be implemented as a separate logical component as well.

Shown is time direction channel calculator **127** which performs the calculation of channel change in the time direction. Frequency direction channel calculator **129** performs the calculation of channel change in the frequency direction. As explained above, the preferred calculation is the inner product of the two pilot assisted channel estimates being compared. Though time direction channel calculator **127** is shown as being illustrated to the right of frequency direction channel calculator **129**, this does not mean that the time direction channel calculation is necessarily to be performed first or that the calculations cannot be performed simultaneously. Either calculation can be performed first, or both can be performed simultaneously. Channel direction comparator **131** compares the results of the calculations performed by both direction channel calculator **127** and frequency direction channel calculator **129** for the purpose of comparing and ascertaining which channel direction, time or frequency, changes slower. Channel direction selector **133** selects which of the two directions changes slower. Block **135** is utilized to interpolate, first in the direction of slower change, and then in the direction of faster change, in accordance with conventional means.

In operation, time direction channel calculator **127** receives two pilot assisted channel estimates and performs the calculation of channel change in the time direction. Frequency direction channel calculator **129** performs the calculation of channel change in the frequency direction though these two calculations can be performed in different order or simultaneously. Channel direction comparator **131** compares the results of the calculations performed by both direction channel calculator **127** and frequency direction channel calculator **129** and compares which channel direction, time or frequency, changes slower. Channel direction selector **133** selects the direction of slower change and interpolation is then performed by block **135** in that direction first, and then in the direction of faster change in accordance with conventional means.

FIGS. **13** to **18** each provide a specific example of a communication system or elements of a communication system that could be used to implement embodiments of the invention. It is to be understood that embodiments of the invention can be implemented with communications systems having architectures that are different than the specific example, but that operate in a manner consistent with the implementation of the embodiments as described herein.

Numerous modifications and variations of the present invention are possible in light of the above teachings. It is therefore to be understood that within the scope of the appended claims, the invention may be practiced otherwise than as specifically described herein.

What is claimed is:

1. A method of inserting pilot symbols into OFDM sub-frames for transmission by a plurality of transmitting antenna, the OFDM sub-frames having a time domain and a frequency domain, each OFDM sub-frame comprising a plurality of OFDM symbols, the method comprising:

for each sub-frame, defining a set of at least two OFDM symbols that are to contain pilot symbols for the sub-frame, wherein none of the OFDM symbols of the set are consecutive in time; and

at each antenna of said plurality of transmitting antennas, inserting pilot symbols in each OFDM symbol of the set in a scattered pattern that does not interfere with the scattered pattern inserted at any other antenna of said plurality of transmitting antennas;

wherein the scattered patterns of the respective antennas are identical but staggered in the frequency domain;

wherein the scattered pattern for each antenna is not frequency-adjacent to the scattered pattern for any other antenna.

2. The method of claim 1, wherein the scattered patterns are regular diamond lattices.

3. The method of claim 1, wherein the scattered patterns are irregular diamond lattices.

4. The method of claim 1, wherein the scattered patterns are kite shaped.

5. The method of claim 1, wherein the number of OFDM symbols per OFDM sub-frame is 7.

6. The method of claim 1, wherein each OFDM sub-frame comprises 8 sub-carriers.

7. The method of claim 1, wherein each OFDM sub-frame comprises 10 sub-carriers.

8. The method of claim 1, wherein each OFDM sub-frame comprises 12 sub-carriers.

9. The method of claim 1, wherein the pilot symbols are inserted in each of the set of at least two OFDM symbols.

10. The method of claim 1, wherein the scattered patterns are cyclically offset, both in a time direction and in a frequency direction.

11. The method of claim 1, wherein the scattered patterns are cyclically offset, both in a time direction and in a frequency direction.

12. The method of claim 1, wherein each sub-frame comprises first, second, third, fourth, fifth, sixth and seventh OFDM symbols in sequence, and wherein said set of at least two OFDM symbols comprises the first and fourth OFDM symbols.

13. An OFDM transmitter, comprising:

one or more transmit antennas;

the OFDM transmitter being adapted to insert pilot symbols into OFDM sub-frames for transmission by the plurality of transmit antennas, the OFDM sub-frames having a time domain and a frequency domain, each OFDM sub-frame comprising a plurality of OFDM symbols, wherein the OFDM transmitter is further configured to:

for each sub-frame, define a set of at least two OFDM symbols that are to contain pilot symbols for the sub-frame, wherein none of the OFDM symbols of the set are consecutive in time; and

at each antenna of said plurality of transmit antennas, insert pilot symbols in each OFDM symbol of the set in a scattered pattern that does not interfere with the scattered pattern inserted at any other antenna of said plurality of transmit antennas;

wherein the scattered patterns of the respective antennas are identical but staggered in the frequency domain;

wherein the scattered pattern for each antenna is not frequency-adjacent to the scattered pattern for any other antenna.

14. A non-transitory memory medium for inserting pilot symbols into OFDM sub-frames for transmission by a plurality of transmitting antenna, the OFDM sub-frames having a time domain and a frequency domain, each OFDM sub-frame comprising a plurality of OFDM symbols, wherein the memory medium stores program instructions, wherein the program instructions are executable by one or more processors to implement:

for each sub-frame, defining a set of at least two OFDM symbols that are to contain pilot symbols for the sub-frame, wherein none of the OFDM symbols of the set are consecutive in time; and

at each antenna of said plurality of transmitting antennas, inserting pilot symbols in each OFDM symbol of the set in a scattered pattern that does not interfere with the scattered pattern inserted at any other antenna of said plurality of transmitting antennas;

wherein the scattered patterns of the respective antennas are identical but staggered in the frequency domain;

wherein the scattered pattern for each antenna is not frequency-adjacent to the scattered pattern for any other antenna.

* * * * *