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Gonikberg

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(54) **EFFICIENT PARTIAL RESPONSE EQUALIZATION**
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(*) Notice: Subject to any disclaimer, the term of this patent is extended or adjusted under 35 U.S.C. 154(b) by 441 days.

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This patent is subject to a terminal disclaimer.

(Continued)

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(57) **ABSTRACT**

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A reduced state maximum likelihood sequence estimator allows the use of improved equalization techniques that provides greatly improved performance for channels with severe attenuation and spectral nulls. The reduced state maximum likelihood sequence estimator retains k_n states of a total number of K states, $k_n < K$, with each retained state having an associated state metric. $(J)(k_n)$ new states are determined based on k_n previous states and a most recently received sample, using J transitions, J being a less than L , where L is a size of a symbol alphabet. $(J)(k_n)$ new state metrics are determined which are respectively associated with each new state. The new state metrics are compared to a threshold and those states whose metric does not exceed the threshold are retained. The reduced complexity of the MLSE allows for the use of partial response equalizers, e.g., a partial response class V (PRV) equalizer. The number of retained states k_n varies according to an adaptive threshold which limits the number of retained states between a lower bound and an upper bound. The threshold may be determined according to the metric of the most likely state of the retained states and a selected one of a plurality of transition metrics associated with the most likely state metric.

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(63) Continuation of application No. 09/249,990, filed on Feb. 13, 1999, now Pat. No. 6,618,451.

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H03D 1/00 (2006.01)
H04L 27/06 (2006.01)

(52) **U.S. Cl.** **375/341; 375/229**

(58) **Field of Classification Search** **375/341, 375/262, 265, 229, 234, 348, 346; 714/792, 714/795; 708/323**

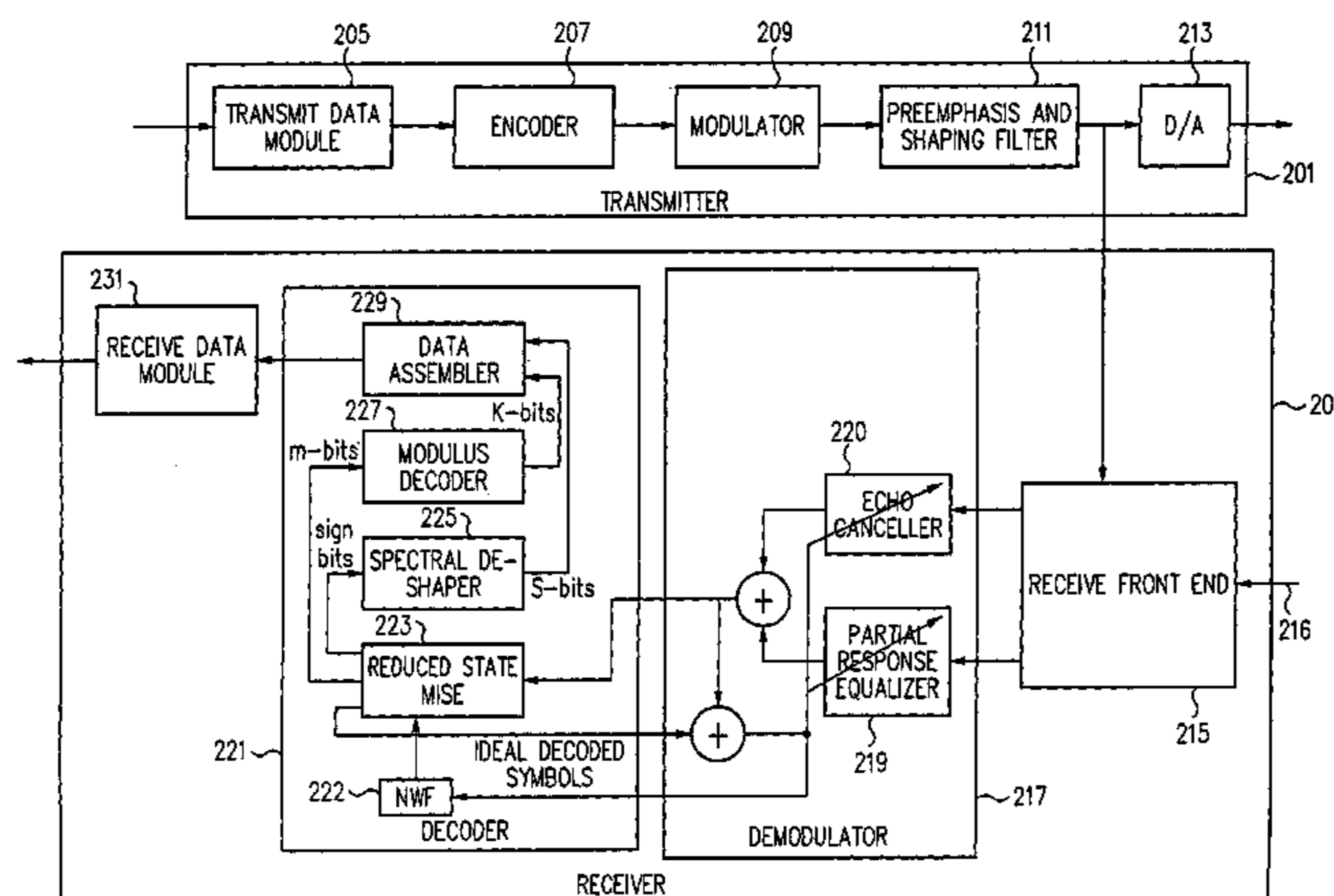
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24 Claims, 3 Drawing Sheets



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$$\begin{array}{l}
 S_1 \{0,0\} \\
 S_2 \{0,1\} \\
 S_3 \{1,0\} \\
 S_4 \{1,1\} \\
 \hline
 S \quad D
 \end{array}
 \begin{array}{l}
 \left[\begin{array}{l}
 d_1 \\
 d_2 \\
 d_3 \\
 d_4
 \end{array} \right]
 \end{array}
 \begin{array}{l}
 A \in (0,1) \\
 L = 2
 \end{array}$$

FIG. 1

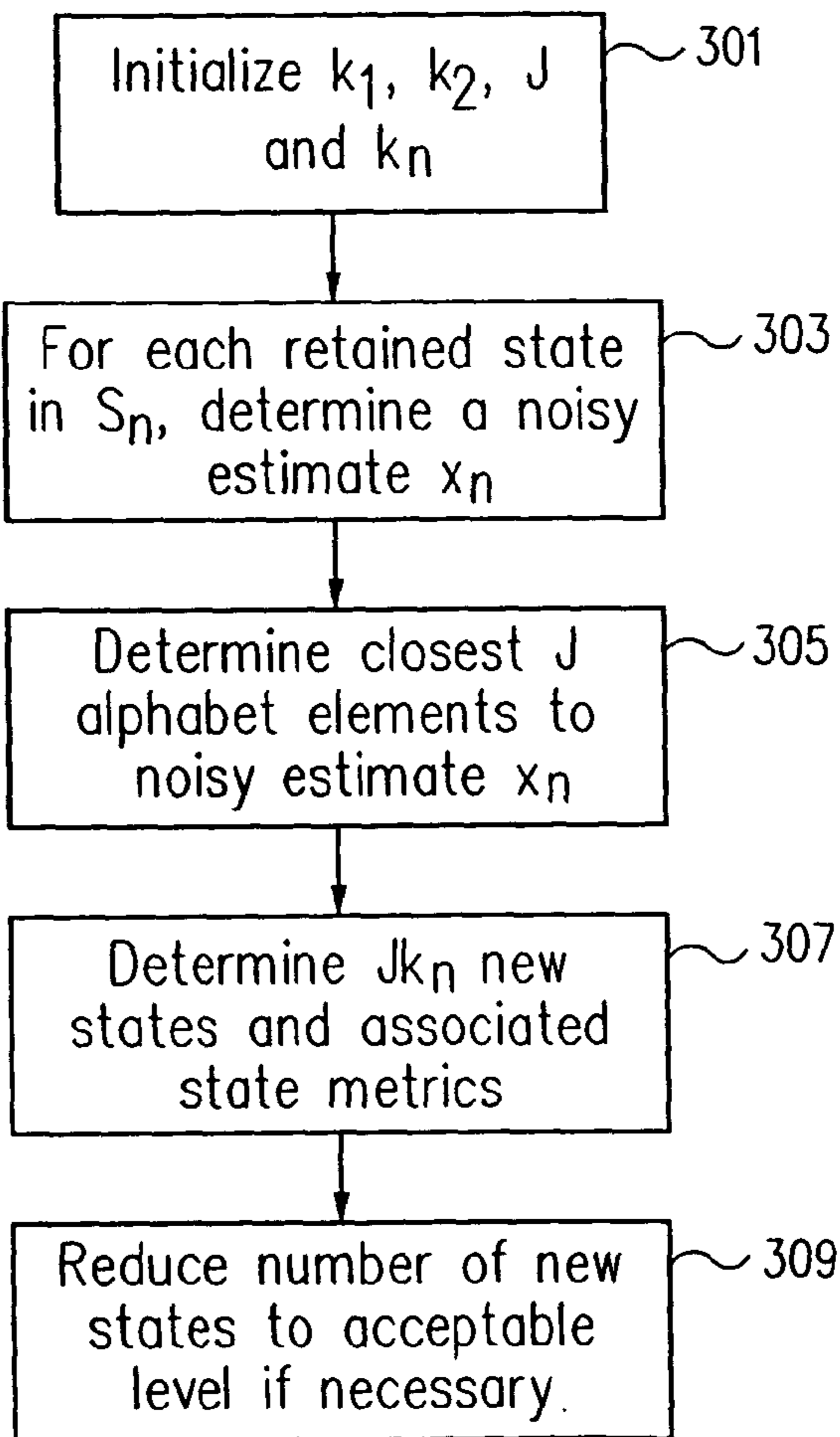


FIG. 3

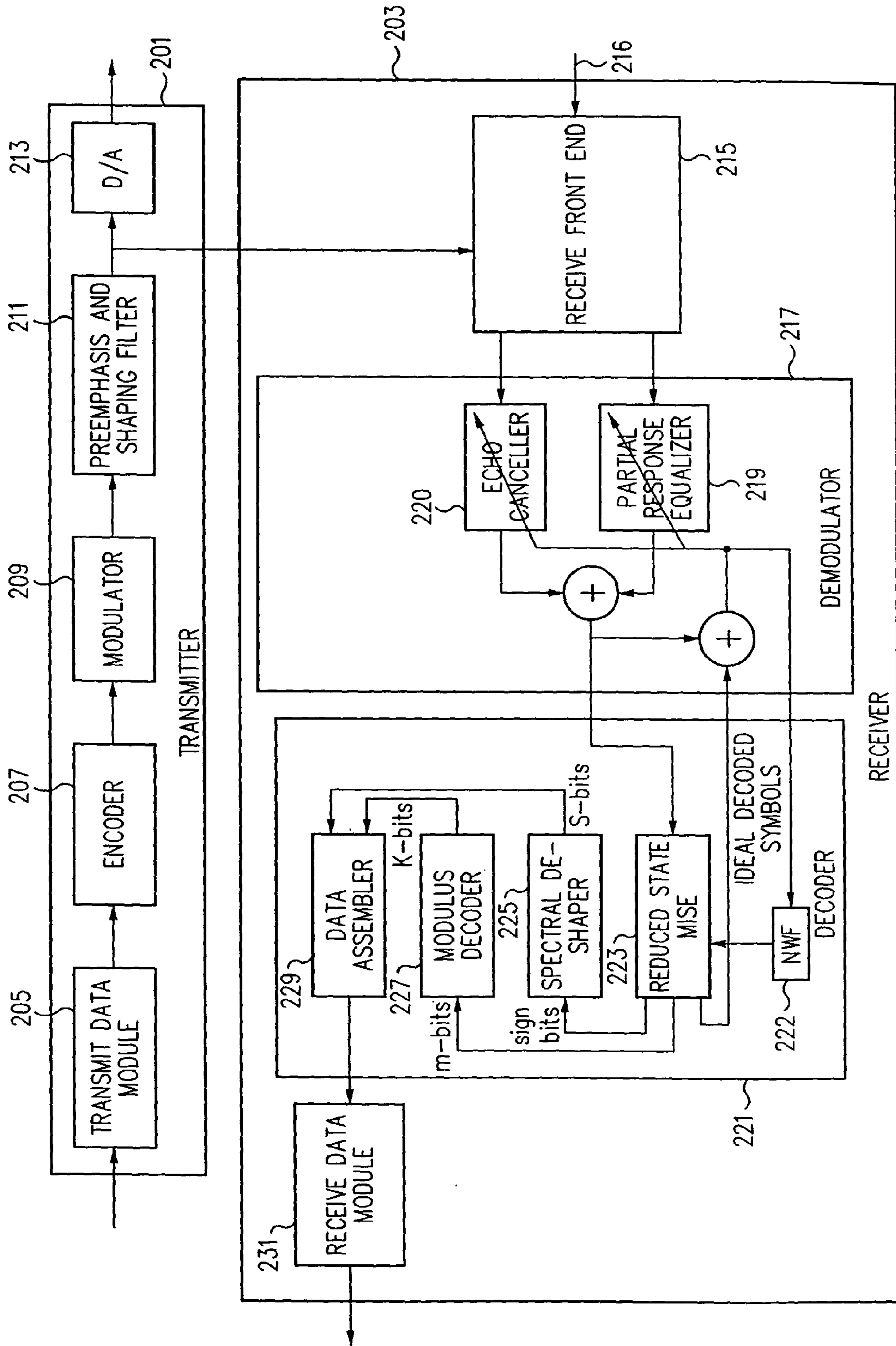


FIG. 2

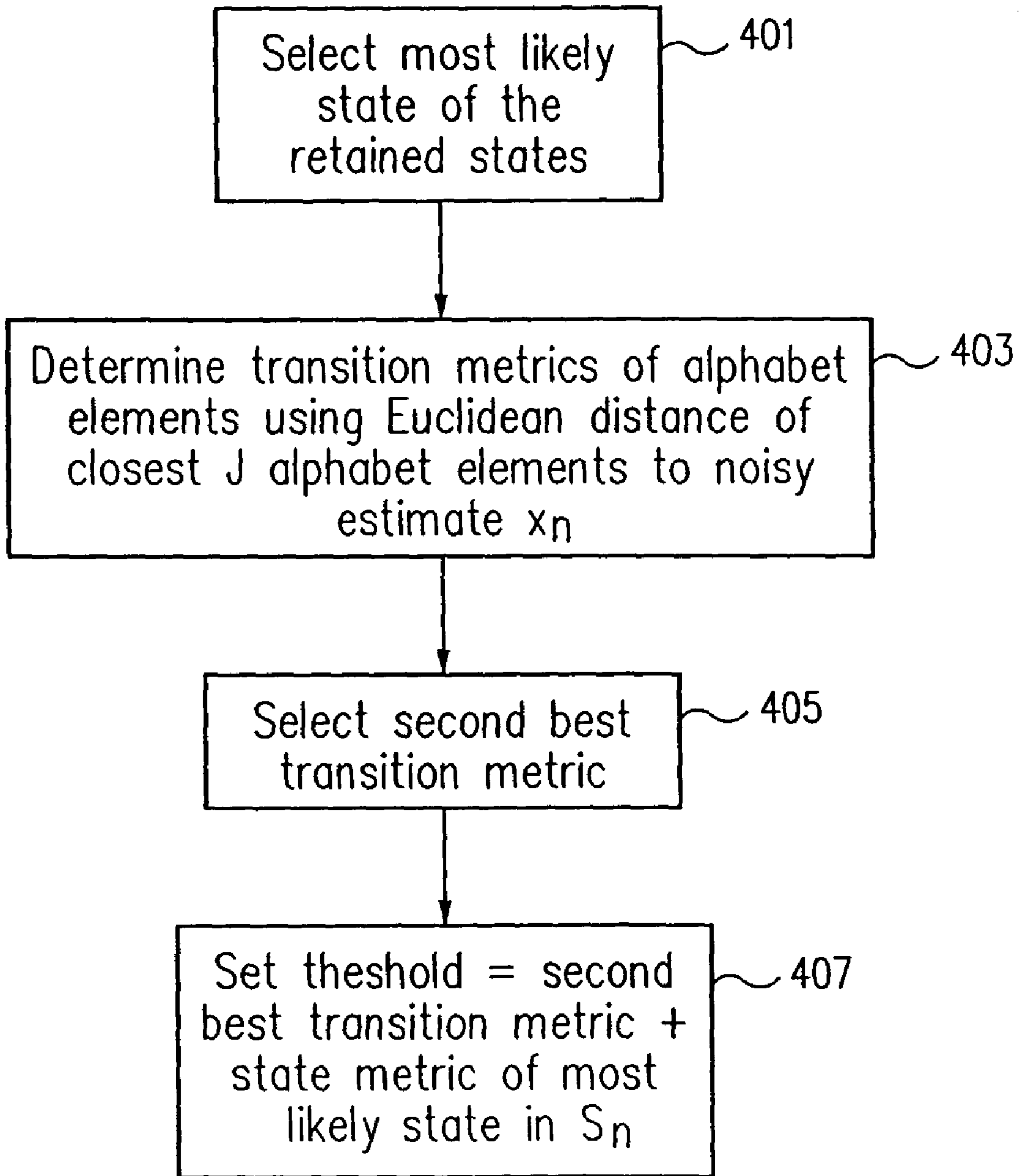


FIG. 4

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EFFICIENT PARTIAL RESPONSE
EQUALIZATIONCROSS-REFERENCE TO RELATED
APPLICATION(S)

This application is a continuation of application Ser. No. 09/249,990, filed Feb. 13, 1999, now U.S. Pat. No. 6,618,451, the entirety of which is incorporated herein by reference.

BACKGROUND

1. Field of the Invention

This invention relates to data communications and in particular to efficient partial response equalization.

2. Description of the Related Art

The received signal in a digital communication system includes noise and distortion caused at least in part by intersymbol interference (ISI). One such digital communication system employs modems, which use digital modulation techniques to modulate and demodulate binary data over analog band-limited communications channels, e.g., telephone lines.

Modems typically conform to international standards to ensure interoperability with modems from other manufacturers. One such standard is the V.34 specification described in ITU-T Recommendation V.34, *A Modem Operating at Data Signalling Rates of up to 28 800 bits/s for Use on the General Switched Telephone Network and on Leased Point-to-Point 2-Wire Telephone-Type Circuits*, dated September, 1994 (previously CCITT Recommendation V.34), which is hereby incorporated herein, in its entirety, by reference. Another such standard is the V.90 specification described in ITU-T Recommendation V.90, *A Digital Modem and Analogue Modem Pair For Use on the Public Switched Telephone Network (PSTN) At Data Signalling Rates of Up To 56 000 bits/s Downstream and Up To 33 600 bits/s Upstream*, dated September, 1998, which is hereby incorporated herein, in its entirety, by reference.

Maximum Likelihood Sequence Estimators (MLSE) are widely used in data communications such as modem communications for decoding data passed through the channels with intersymbol interference (ISI) and for decoding convolutionally encoded data. The Viterbi algorithm (VA) is quite often used to implement MLSE. A brief description of the Viterbi algorithm, which is well known in the art, is provided to facilitate an understanding of the present invention.

Assume that a sequence of symbols $x = \{x_i\}$, $i \in [-\infty; \infty]$, $x_i \in A = \{a_1, a_2, \dots, a_L\}$ is transmitted through a channel with impulse response $h = \{h_i\}$, such that $h_i \neq 0$ only when $0 < h_i \leq M$, where $M-1$ is the number of history terms contained in the channel. The signal received at the other end of the channel in the absence of noise is defined as $y = x * h$, where "*" denotes a convolution. If the noise η is added to the signal in the channel, then the signal at the other end of the channel contains that noise and is defined as $z = y + \eta$. The receiver must reconstruct the transmitted sequence of symbols x , based on the received sequence z . At the time nT the following can be used to reconstruct the most recently sent symbol x_n :

$$x_n = (y_n - (x_{n-1}h_1 + \dots + x_{n-M+1}h_{M-1})) / h_0 \quad (1)$$

From the equation (1) it can be seen that besides the received signal y_n , value x_n depends on the vector $\{x_{n-1}, \dots, x_{n-M+1}\}$ of $M-1$ previously decoded symbols. That vector

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will be further referred to herein as a state. With each new decoded symbol, the state of the decoder changes to reflect the new value of the vector $\{x_{n-1}, \dots, x_{n-M+1}\}$. That is, if at a time nT the state was $\{x_{n-1}, \dots, x_{n-M+1}\}$ then at a time $(n+1)T$ the new state will be $\{x_n, \dots, x_{n-M+2}\}$ and so forth. That change will be further referred to herein as a state transition. The history of state transitions represents a state trajectory. Since each symbol x_n belongs to a finite alphabet A of size L , there can only be $K = L^{M-1}$ unique states. All states comprise a state set $S = \{s_1, s_2, \dots, s_K\}$, where each element s_k is a vector of $M-1$ elements that belong to alphabet A such that $s_k \neq s_m$ for $k \neq m$.

Since the noiseless channel output y_n is not available to the receiver, the value of x_n cannot be determined with absolute certainty, and instead an estimate is used:

$$x_n = (z_n - (x_{n-1}h_1 + \dots + x_{n-M+1}h_{M-1})) / h_0 \quad (2)$$

The Euclidean distance, t_{n1} , from the alphabet element a_1 to the estimate x_n , is defined as $t_{n1} = (x_n - a_1)^2$, which provides the measure of likelihood that the transmitted symbol x_n equals a_1 at the time nT .

In a simple receiver, the alphabet element with the minimum Euclidean distance is selected and x_n is assumed to be equal to that alphabet element. However if x_n is not determined correctly (e.g. due to noise), that incorrect value will cause an incorrect state transition causing future symbols to be decoded incorrectly affecting in turn future state transitions and so on. That condition is called "error propagation."

To avoid the "error propagation" problem, all possible decoder states and all possible state transitions must be examined. A state metric $D_n = \{d_{n1}, d_{n2}, \dots, d_{nK}\}$ defines the measure of likelihood, such that each element d_{nk} defines the measure of likelihood of state s_k at a time nT which is directly related to the Euclidean distance of the elements of the symbol vector corresponding to state s_k . The relationship of the state metric D and state set S is shown in FIG. 1 in which set S is shown to consist of four states s_1 through s_4 . In the example shown in FIG. 1 $A \in (0,1)$, $L=2$, and $M=3$. Each state s_1 through s_4 has an associated state metric d_1 through d_4 in D .

1. For each state s_k of a set S , calculate a symbol estimate x_{nk} , based on received symbol z_n according to equation (2) above.
2. For each state s_k of a set S , consider L transitions from that state, and for each transition combination $(k,1)$ calculate a combined metric $d_{k1} = d_k + t_{k1}$, where t_{k1} is a Euclidean distance of the alphabet element a_1 from the symbol estimate x_{nk} , $t_{k1} = (x_{nk} - a_1)^2$.
3. For each state s_k of a set S , consider L transitions to that state, selecting the one with the minimum combined metric d calculated during step 2 and assign its value to the state metric d_k .
4. Find the state with the minimum metric d_k storing a transition that led to that state as a candidate optimal trajectory.
5. The first four steps are repeated for each value of n , i.e., for each received symbol.

The optimal trajectory for the state with the smallest metric is considered the optimal path (most likely sequence) at a given time. As it can be seen from the above description, the computational complexity of the Viterbi algorithm is proportional to L^M . For high speed communication systems over band limited channels the value of L is large, thus making the Viterbi algorithm complexity potentially prohibitive even for channels with relatively short impulse response.

One use of the Viterbi algorithm, as stated above, is in modem data transmission. Such transmission is always affected by linear intersymbol interference (ISI) and by noise. Those two impairments are typically countered by equalization, a technique which minimizes ISI and noise at periodic instances at which decisions are taken. The ultimate goal of the equalizer is to minimize a combined effect of ISI and noise and thus reduce the probability of incorrect decisions. Traditionally, dial up modem designers used Linear Equalizers (LE) to do the job. The performance of LE is quite satisfactory when the combination of the channel impulse response and the equalizer can form a Nyquist-1 pulse to satisfy the distortionless (zero ISI) criterion. To achieve that goal, the bandwidth of the channel has to be wider than the symbol rate employed by the modem.

The new generation of modems conforming to the V.90 recommendation no longer satisfy this criterion. The impulse response of a PCM codec is designed to achieve satisfactory transmission of voice signals, and its bandwidth is always more narrow than the 8000 Hz symbol rate used by a modem conforming to the V.90 standard. The spectral nulls at DC and 4000 Hz generate infinite noise enhancements when LE is employed. To reduce such noise enhancements, more advanced equalization techniques should be used. Those are decision feedback equalizers (DFE) and partial response equalizers (PRE). Although usually treated separately, LE and PRE are just special cases of DFE. DFE includes two portions: the forward equalizer (FE) and the feedback equalizer (FBE). Both the FE and the FBE can be implemented as linear FIR filters, where the input samples serve as an input to the FE and the previously decoded symbols serve as input to the FBE. The output of both the FE and the FBE are added together and the result is used as the basis for decisions for determining the transmitted signal. DFE allows some ISI to remain at the output of FE to be then canceled by FBE. It has been shown that DFE can be the optimum receiver with no decision delay. When used in conjunction with Viterbi detector, (VD) DFE becomes a powerful tool in battling ISI even for channels with spectral nulls.

However the implementation of a Viterbi detector grows considerably more complex with number of levels used by the transmission symbols and by number of taps in the FBE. The computational complexity of a Viterbi detector is proportional to L^M where M is the number of FBE taps and L is the size of the transmitted symbols alphabet.

Partial response equalizers (PRE), being a special case of DFE are used to reduce the computational complexity of the Viterbi detector by forcing the FE to leave uncanceled only a controlled amount of ISI, thus requiring only a small number of FBE taps to cancel it. The combination of channel impulse response and FE of PRE form a response, called Partial Response (PR), which contains only a few, usually integer-valued coefficients, thus allowing controlled levels of ISI from a small number of symbols to be present at the instances of decision making. A Viterbi detector is then employed to remove that ISI and make the most probable decision. The choice of partial response depends heavily on the transmission channel. When spectral characteristics of the partial response match those of a channel, the FE has an easier task and noise enhancement is limited. For a channel with spectral nulls, it is highly desirable to use a partial response having spectral nulls at the same positions to avoid infinite noise enhancement. A pulse code modulation (PCM) channel has two spectral nulls: one around DC, another around 4000 Hz, thus confining the choice of the partial response for PCM modem to those with the same spectral

nulls. Class IV Partial Response (PRIV) often called modified duobinary, has long been used for the channels with similar characteristics and is well known in the art.

The PRIV FE output contains the difference of two symbols spaced by two symbol intervals:

$$y_n = x_n - x_{n-2}$$

Since ISI from only one symbol is present, the number of states of the Viterbi detector equals L—the size of the symbol alphabet. For data rates achievable by a V.90 compliant modem, $L \leq 128$. Although implementation of 128-state Viterbi decoder is not trivial, Set Partitioning, a well known technique in the art, can be used to reduce the number of Viterbi detector states to a more manageable number. However, when the channel has severe attenuation at a wider range of frequencies adjacent to DC and 4000 Hz, the noise enhancement by a class IV partial response equalizer becomes intolerable.

Therefore, it would be desirable to utilize a partial response equalizer that does not exhibit intolerable noise enhancement and to have the performance of a Viterbi decoder with manageable complexity.

SUMMARY

Accordingly the invention provides a reduced state maximum likelihood sequence estimator that causes only a slight degradation of performance relative to an implementation of a full state Viterbi decoder. That allows the use of improved equalization techniques that greatly improve performance for channels with severe attenuation and spectral nulls.

In one embodiment of the invention, a method is provided for implementing a reduced state maximum likelihood sequence estimator in a communications system to decode a received signal. The method includes retaining k_n states of a total number of K states, $k_n < K$, each retained state having an associated state metric. $(J)(k_n)$ new states are determined based on k_n previous states and a most recently received symbol, using J transitions, J being a less than L, where L is a size of a symbol alphabet. $(J)(k_n)$ new state metrics are determined which are respectively associated with each new state. The new state metrics are compared to a threshold and those states whose metric does not exceed the threshold are retained.

In another embodiment, the invention provides a modem that includes a partial response class V (PRV) equalizer coupled in its receive path. In still another embodiment of the invention a modem includes a reduced state maximum likelihood sequence estimator (MLSE) in its receive path. That MLSE may be coupled to a partial response equalizer. The reduced state maximum likelihood sequence estimator retains a varying number of reduced states. The number of retained states may be limited by use of an adaptive threshold that limits the number of retained states between a lower bound and an upper bound. The threshold may be determined according to a metric of a most likely state of the retained states and a selected one of a plurality of associated transition metrics.

BRIEF DESCRIPTION OF THE DRAWINGS

The present invention may be better understood, and its numerous objects, features, and advantages made apparent to those skilled in the art by referencing the accompanying drawings, wherein the use of the same reference symbols in different drawings indicates similar or identical items.

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FIG. 1 illustrates the state vector and state metric utilized in Viterbi decoding.

FIG. 2 illustrates an exemplary modem incorporating an embodiment of the present invention.

FIG. 3 is a flow chart illustrating how reduced states and reduced transitions are utilized in an embodiment of the present invention.

FIG. 4 is a flow chart illustrating the method of determining the threshold according to one embodiment of the invention.

DESCRIPTION OF THE PREFERRED EMBODIMENT(S)

The current invention provides an approach which addresses the issue of computational complexity of the Viterbi algorithm by offering an efficient approach which, while being suboptimal, causes only a slight degradation of performance relative to an implementation of a full state Viterbi decoder. That allows the use of improved equalization techniques.

As discussed above, when the channel has severe attenuation at a wider range of frequencies adjacent to DC and 4000 Hz, the noise enhancement caused by the use of a PRV equalizer becomes intolerable. One approach to battle this noise enhancement is to use Partial Response class V (PRV) equalizer. PRV FE output contains the second difference of symbols spaced by two symbol intervals, and can be expressed as:

$$y_n = x_n - 2x_{n-2} + x_{n-4}$$

The PRV equalizer has double nulls at DC and 4000 Hz and thus produces much less noise enhancement for channels with high attenuation at band edges. PRV equalizers were never considered practical for multilevel signals such as those received in modems conforming to the V.90 standard, because of the huge number of states required by Viterbi decoding. For example, a straightforward Viterbi implementation for a data rate of 56 Kbits/sec having 128 symbols, requires 16,384 states. Such an implementation requires a significant amount of memory to store the states as well as having high computational complexity because of the large number of states. Computational complexity of such Viterbi decoding is enormous even when set partitioning is employed. Plain decision-driven FBE cannot be used because of stability considerations. Even a single decision error will cause a subsequent chain reaction without any chance for recovery. The efficient reduced state MLSE disclosed herein allows the use of a wide variety of partial response equalizers with performance close to that achieved by a full state Viterbi decoder without the enormous computational load required by a full state Viterbi decoder.

Another aspect of equalizer implementation is the tap spacing. T-spaced equalizers use the signal sampled at the symbol rate. Fractionally spaced equalizers (FSE) operate on a signal sampled at a rate higher than the symbol rate and require eventual down sampling. It is known that T-spaced equalizers depend heavily on coded sample clock phase, and that there is at least one value of the phase in the symbol interval T for which the combined channel response and equalizer response have spectral nulls at half symbol rate. To avoid this undesirable effect, modem designers traditionally employed FSE in spite of its higher computational complexity. However since PRV equalizers actually require spectral null at half symbol rate, the advantage of FSE becomes non-existent. Therefore a T-spaced equalizer is a logical

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choice for a V.90 modem. Use of T-spaced equalizer also allows the use of 8 KHz sample rate for the A/D converter.

A block diagram of an exemplary V.90 modem employing an embodiment of a reduced state maximum likelihood sequence estimator and a class V partial response equalizer according to the present invention is shown in FIG. 2. A brief description of the modem shown in FIG. 2 will provide the appropriate context for better understanding the embodiments of the invention described herein. A detailed discussion of the operation of the exemplary modem is not provided as modem operation in conformance with, e.g., the V.90 recommendation, is known the art. In one embodiment, the MLSE and partial response equalizer shown in FIG. 2 are implemented in software which may be stored on computer readable media which can be executed on a general purpose processor. Those of skill in the art will appreciate that the teachings herein may also be applied to a variety of modem implementations such as those using a digital signal processors and/or stand alone processors.

The block diagram of the modem shown in FIG. 2 includes transmitter 201 and receiver 203. The transmitter data module 205 supplies bits to the encoder 207. The transmitter data module 205 either generates those bits locally in the case of training or fetches them from the external data source in the case of data mode. It then scrambles the bits as required and passes the data to the encoder 207. Encoder 207 converts the input bit stream from data module 205 into a sequence of symbols which are then provided to modulator 209. Modulator 209 performs appropriate sampling and filtering operations and provides its output to shaping and pre-emphasis filter 211 that provides square-root-of raised cosine shaping as well as pre-emphasis filtering specified by the V.90 recommendation. That output is provided to the digital-to-analog converter 213.

The receiver portion of the modem 203 receives the output from the transmitter (prior to the D/A) into receiver front end 215. Receiver front end 215 also receives the signal 216 from the channel. Receiver front end 215 performs such operations as analog-to-digital conversion on the received signal, various filtering and echo-canceling operations and provides its output to the demodulator 217. The demodulator 217 includes partial response class V equalizer 219 as described further herein. The demodulator 217 also includes the second stage near end echo canceller 220, which cancels the echo at the output of the equalizer and is intended to track slow variations of the echo signal. The output of the partial response equalizer is provided to the decoder 221 and more specifically to the reduced state maximum likelihood sequence estimator 223, as described further herein.

Note that the noise signal at the output of PRV equalizer is strongly colored due to the nature of the partial response used. A noise-whitening filter is required to achieve optimal performance of the MLSE. The noise-whitening filter 222 is designed as an error predictor. It is trained during the reception of a TRN signal during a training phase and then used in conjunction with the MLSE to minimize the error probability.

The symbols decoded by MLSE 223 are then split into sign and amplitude components and passed respectively to the spectral de-shaper 225 and modulus decoder 227. Both of those modules extract the data payload from the symbols that is later converted to a bit stream by data assembler 229. Receive data module 231 descrambles this bit stream and passes it to the application program.

While a V.90 modem has been described, it should be understood that other modems and other communication devices may advantageously use the invention described herein.

Referring still to the block diagram shown in FIG. 2, the partial response equalizer 219 provides its output, $(y_n = x_n - 2x_{n-2} + x_{n-4})$, to the reduced state MLSE 223. Because it is a reduced state estimator, at any given time, nT , the reduced state MLSE described herein retains only a reduced number of states k_n . Note that k_n can vary, having a lower bound and an upper bound such that $k_1 \leq k_n \leq k_2$. A further simplification as compared to the full state Viterbi detector is that only a reduced number of transitions, J , are analyzed, $J < L$, L being the size of the alphabet.

The advantages of the reduced state approach described herein are readily apparent when compared with a full state Viterbi decoder implementation. For example, for a full Viterbi decoder, 16,384 states can be required for a modem conforming to the V.90 recommendation (alphabet of 128). In comparison, in one embodiment of the invention described herein, the reduced number of states may be only 12. Further, only two transitions ($J=2$) from those retained states are analyzed rather than L transitions (L being the size of the alphabet, e.g. 128). The parameters k_1 and k_2 are parameters of the reduced state MLSE which can be selected to adaptively control tradeoff between performance and computational complexity. In addition, J can also be adjusted to increase and/or reduce the complexity.

Referring to FIG. 3, the flowchart illustrates generally an embodiment of the reduced state estimator. The parameters k_1 , k_2 , k_n , and J are initialized. Some or all of the parameters may be implemented as programmable or may be fixed. Exemplary values are: $k_1=8$, $k_2=16$, $k_n=12$, and $J=2$. In 303, a noisy estimate of the received signal is determined for each of the retained states. Next, the MLSE determines the closest J alphabet elements to the noisy estimate in 305. In 307, the MLSE, using the J alphabet elements, determines the $(J)(k_n)$ new states. Thus, if there are 12 states in k_n , and $J=2$, then 24 new states will be generated. The transition metric associated with each alphabet element is added to the state metric for each of the retained states to determine a state metric associated with each of the new states. Finally, if the number of new states is outside the range of k_1 and k_2 , then the number of new states are adjusted accordingly.

If the number of new states is greater than k_2 , the new states must be reduced down to the desired number of retained states. Otherwise, the number of retained states will grow, quickly causing the computational complexity to be burdensome. Therefore, if $(J)(k_n)$ (the number of new states) $> k_2$, the MLSE discards those states with the largest metrics such that $k_1 \leq$ the number of the remaining states $\leq k_2$. In that way, the number of retained states is manageable.

One approach to select the appropriate ones of the new states to retain is to sort the temporary state metrics in ascending order, and then select the first k_n new states to become the retained states. However sorting is an expensive operation with complexity of the order (k_n^2) . If k_1 and k_2 are large, sorting may become the dominant operation of the overall algorithm. An alternative to sorting is to determine an empirically based threshold "t." The metrics of the new states are compared to the threshold. Those new states whose metric is below the threshold are retained. One way to calculate the threshold "t" is as follows:

$$t = ((k_1 + k_2) / (2Jk_n)) (1 / Jk_n) \sum d_{jn+1}$$

That formula is designed to provide a threshold that is adaptive according to the number of retained states. Assume that $k_1=8$, $k_2=16$, $J=2$, and the target k_n is 12. If the number of new states $(J)(k_n)$ is exactly twice the target of 12, i.e. the number of retained states is exactly the target, then the first term of the equation above provides $(1/2)$. That term is used to adjust the average metric of the new states determined by

$$(1 / Jk_n) \sum d_{jn+1}$$

If the number of retained states is exactly the target of 12, then $(1/2)$ of the average metric is selected as the target. Note that the average is used to provide an estimate of the median. If the number of retained states is less than the target k_n , the next threshold adjusts to be somewhat higher than $1/2$ of the average metric. Alternatively, if the number of retained states is greater than the target, then the next threshold adjusts to be below $(1/2)$ of the average metric. In that way, the threshold continually adapts to the actual number of retained states and fluctuates around the target k_n .

A new threshold is typically determined for every new received symbol. All states are selected as retained states whose metric is less than threshold (t). This threshold approach has a complexity of the order (k_n) and is much more efficient for large k_1 , k_2 . It however does not guarantee that the resulting number of states selected from the new states are in the range $[k_1:k_2]$.

In case the number of states selected from the new states are not in the range of $[k_1:k_2]$, the threshold has to be adjusted and selection repeated. If the threshold needs adjusting, it can be adjusted up or down, as needed by a fixed percentage, e.g., 25% or some other percentage appropriate to the particular implementation. Thus, if there are too few retained states, ($<k_1$), (t) can be adjusted up 25% and similarly, if there are too many retained states ($>k_2$), (t) can be adjusted down. The wider the range $[k_1:k_2]$ the smaller the chance that repeat selection would be required. In simulation results for the cases where $k_2=2k_1$ repeat selection of the threshold is only required in about 10% of iterations.

Other empirical approaches for determining the threshold t are also possible. For example, another approach is illustrated in FIG. 4. Most of the operations illustrated in FIG. 4 are performed as part of the reduced state approach described herein and do not have to be repeated for determination of the threshold. In 401, the most likely state of the retained states is selected according to its state metric. That is, of the retained states, the most likely state is that having the lowest metric, which is the output of the MLSE. Then, using the noisy estimate x_n of the received signal z_n , the elements of the alphabet closest to x_n are selected and their transition metrics determined. Those elements will have metrics associated with them based on the Euclidean distance from the noisy estimate x_n . In 407, the transition metric is selected. For the case of $J=2$, the transition metric selected is the second best transition metric. That provides a threshold for the next estimate. Then in 407, the threshold is determined as the sum of the previous best state metric and one of the transition metrics. The second best metric is

chosen to provide a threshold that is high enough to generate a sufficient number of retained states. If the threshold is set too low or too high, such that fewer than k_1 or greater than k_2 states would be retained, the threshold may be adjusted up or down accordingly. Note that if J is other than two, a metric other than second best may be chosen. This approach provides an adaptive threshold based on one of the retained states (the best retained state in the embodiment described).

The reduced state MLSE described herein may be used advantageously with a partial response class V equalizer, as illustrated, e.g., in FIG. 2 to provide improved performance over channels with severe attenuation and spectral nulls. The combination of the MLSE and a PRV equalizer is described as follows.

For each of k_n retained values, S_{j_n} , $j=1, 2, \dots, k_n$, of state vector S_n , and received noisy signal z_n , the MLSE calculates a noisy estimate of sent signal x_{j_n} :

$$x_{j_n} = z_n - \sum_{i=1}^{M-1} x_{n-i} h_i$$

In the equation above, M is the memory of the channel in symbol intervals and z_n is the noisy output of the equalizer. For use with the PRV equalizer, in order to determine an estimate of the sent signal, the MLSE has to subtract out the second difference of symbols spaced by two symbol intervals as previously described ($-2x_{n-2} + x_{n-4}$). Therefore in the equation above, $h=-2$ for $i=2$ and $h=1$ for $i=4$. Because $M=5$, four history terms have to be stored for each retained state. Only two of the history terms are used during any particular generation of the noisy estimate. A noisy estimate is generated for each of the retained states using the stored history values and the output of the PRV.

The next operation of the MLSE is to determine J elements from alphabet A for each estimate x_{j_n} , such that the Euclidean distance from these elements to x_{j_n} is the smallest. Assuming J is two, the two alphabet elements closest to each noisy estimate, x_{j_n} , are selected. If the noisy estimate is below the lowest alphabet element or above the largest element, the first or last two alphabet element are chosen, respectively.

Finally, the MLSE calculates $(J)(k_n)$ temporary new states for state vector S_{n+1} , and state metric D_{n+1} , having a metric associated with each of the states in state vector S_{n+1} .

Thus, continuing with the assumption that $k_n=8$ and $J=2$, 16 new states will be calculated. In addition, 16 state metrics are determined that are associated with the new states. The new state metrics are based on the prior state metric and the transition metric associated with the J transitions selected. The transition metrics, as is known in the art, are determined according to the Euclidean distance between the J alphabet points and the noisy estimate.

Each new state is generated using the elements (alphabet values) from the previous state, by deleting the oldest element and inserting as the newest element, the alphabet element representing the received value that transitioned the previous state in S_n to the current state in S_{n+1} .

As described previously, various threshold techniques may be employed to reduce the new states to the appropriate number. If necessary, the threshold may be increased or decreased to increase or reduce, respectively, the number of retained states. As with the rest of the MLSE and the PRV equalizer described herein, the operation of determining and adjusting the threshold may be implemented in software instructions operating on a digital signal processor and/or a general purpose processor.

The description of the invention set forth herein is illustrative, and is not intended to limit the scope of the invention as set forth in the following claims. For instance while the reduced state MLSE described herein was described in association with a partial response class V equalizer, the reduced state MLSE described herein may be employed wherever Viterbi decoding has been used, for example in decoding convolutionally encoded data or in conjunction with different classes of partial response equalizers. Additionally, while the communication device described was a modem complying with the V.90 standard, other telecommunication devices may also benefit from the invention described herein and the invention should not be considered as being limited to a particular type of communication device or to a particular modem implementation. Variations and modifications of the embodiments disclosed herein, may be made based on the description set forth herein, without departing from the scope and spirit of the invention as set forth in the following claims.

What is claimed is:

1. A communications system, comprising:

a partial-response linear equalizer responsive to at least a first and a second difference of symbols, the partial-response linear equalizer being a class V partial-response linear equalizer coupled in a receive path of the communications system; and

a reduced state maximum likelihood sequence estimator (MLSE) coupled to the partial-response linear equalizer.

2. The communications system of claim 1, wherein the partial-response equalizer has double nulls at half a symbol rate of the communications system.

3. The communications system of claim 1, wherein the partial-response equalizer has double nulls at DC.

4. The communications system of claim 1, wherein the partial-response equalizer has a transfer function

$$y_n = x_n - 2x_{n-2} + x_{n-4},$$

wherein x_n , x_{n-2} and x_{n-4} are first, second and third symbols, respectively.

5. The communications system of claim 1, wherein the MLSE further comprises:

a plurality k_n of retained states, each of the retained states having an associated state metric, k_n being less than a total number of possible states;

a set of $(J)(k_n)$ new states, determined according to J transitions, J being less than a size of a symbol alphabet, and an associated set of new state metrics; and

a threshold for comparison to the new state metrics.

6. The communications system of claim 5, wherein the threshold is adaptive.

7. The communications system of claim 5, wherein k_n is variable.

8. The communications system of claim 5, wherein the MLSE, receiving an output, z_n , of the partial-response linear equalizer, calculates a noisy estimate, X_{j_n} , of a sent symbol, for each of the retained states.

9. The communications system of claim 5, wherein the noisy estimate x_{j_n} of the sent signal is determined according to:

$$x_{j_n} = z_n - \sum_{i=1}^{M-1} x_{n-i} h_i$$

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wherein $M-1$ is the number of stored history terms; $h=-2$ for $i=2$; $h=1$ for $i=4$; z_n is a received noisy signal; and x_{n-i} is a symbol.

10. A method of operating a communications system, the method comprising generating, using an equalizer on a received signal, a class V partial response having at least double nulls approximately where a channel response has spectral nulls or severe attenuation.

11. The method, as recited in claim **10**, further comprising:

providing the output of the equalizer to a reduced state maximum likelihood sequence estimator.

12. The method, as recited in claim **11**, further comprising:

generating an estimate of the transmitted symbol using a variable number of reduced states and the received signal.

13. A communications system comprising:

a partial-response linear equalizer coupled in a receive path of the communications system, the partial-response linear equalizer having a transfer function including at least double nulls approximately where a channel response has spectral nulls or severe attenuation,

wherein the partial-response equalizer has a transfer function:

$$y_n = x_n - 2x_{n-2} + x_{n-4},$$

wherein x_n , x_{n-2} and x_{n-4} are first, second and third symbols, respectively.

14. The communications system of claim **13**, wherein the partial-response equalizer has double nulls at half a symbol rate of the communications system.

15. The communications system of claim **13**, wherein the partial-response equalizer has double nulls at DC.

16. The communications system of claim **13**, wherein the partial-response linear equalizer is a class V equalizer.

17. The communications system of claim **13**, wherein the communications system further comprises a reduced state maximum likelihood sequence estimator (MLSE) coupled to the partial-response linear equalizer, the MLSE including:

a plurality k_n of retained states, each of the retained states having an associated state metric, k_n being less than a total number of possible states;

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a set of $(J)(k_n)$ new states, determined according to J transitions, J being less than a size of a symbol alphabet, and an associated set of new state metrics; and a threshold for comparison to the new state metrics.

18. The communications system of claim **17**, wherein the threshold is adaptive.

19. The communications system of claim **17**, wherein k_n is variable.

20. The communications system of claim **17**, wherein the MLSE, receiving the output z_n , of the partial-response linear equalizer, calculates a noisy estimate, x_{jn} , of a sent symbol, for each of the retained states.

21. The communications system of claim **20**, wherein the noisy estimate x_{jn} of the sent signal is determined according to:

$$x_{jn} = z_n - \sum_{i=1}^{M-1} x_{n-i} h_i$$

wherein $M-1$ is the number of stored history terms; $h=-2$ for $i=2$; $h=1$ for $i=4$; z_n is a received noisy signal; and x_{n-i} is a symbol.

22. An apparatus, comprising:

means for generating a class V partial response having at least double nulls approximately where a channel response has spectral nulls or severe attenuation; and means for generating an estimate of a symbol transmitted over the channel using a variable number of reduced states and a received signal.

23. The apparatus, as recited in claim **22** wherein the channel response has nulls at DC and half a symbol rate of the apparatus.

24. A computer program executable encoded in one or more computer readable media selected from the set of disk, tape, or other magnetic, optical, or electronic storage medium, the computer program executable including instructions for generating a class V partial-response linear equalizer responsive to at least a first and a second difference of symbols and a reduced state maximum likelihood sequence estimator (MLSE), the MLSE receiving the output of the partial-response linear equalizer.

* * * * *

UNITED STATES PATENT AND TRADEMARK OFFICE
CERTIFICATE OF CORRECTION

PATENT NO. : 7,139,337 B2
APPLICATION NO. : 10/651924
DATED : November 26, 2006
INVENTOR(S) : Mark Gonikberg

Page 1 of 1

It is certified that error appears in the above-identified patent and that said Letters Patent is hereby corrected as shown below:

Col. 10, line 40, please replace "k_{n-2}" with --x_{n-2}--

Signed and Sealed this

First Day of June, 2010

A handwritten signature in black ink that reads "David J. Kappos". The signature is written in a cursive, flowing style.

David J. Kappos
Director of the United States Patent and Trademark Office